

**Specification for radio disturbance and immunity
measuring apparatus and methods –**

Part 1-5:

**Radio disturbance and immunity measuring
apparatus – Antenna calibration test sites
for 30 MHz to 1 000 MHz**

*This **English-language** version is derived from the original **bilingual** publication by leaving out all French-language pages. Missing page numbers correspond to the French-language pages.*

Consolidated editions

The IEC is now publishing consolidated versions of its publications. For example, edition numbers 1.0, 1.1 and 1.2 refer, respectively, to the base publication, the base publication incorporating amendment 1 and the base publication incorporating amendments 1 and 2.

Further information on IEC publications

The technical content of IEC publications is kept under constant review by the IEC, thus ensuring that the content reflects current technology. Information relating to this publication, including its validity, is available in the IEC Catalogue of publications (see below) in addition to new editions, amendments and corrigenda. Information on the subjects under consideration and work in progress undertaken by the technical committee which has prepared this publication, as well as the list of publications issued, is also available from the following:

- **IEC Web Site** (www.iec.ch)

- **Catalogue of IEC publications**

The on-line catalogue on the IEC web site (www.iec.ch/searchpub) enables you to search by a variety of criteria including text searches, technical committees and date of publication. On-line information is also available on recently issued publications, withdrawn and replaced publications, as well as corrigenda.

- **IEC Just Published**

This summary of recently issued publications (www.iec.ch/online_news/justpub) is also available by email. Please contact the Customer Service Centre (see below) for further information.

- **Customer Service Centre**

If you have any questions regarding this publication or need further assistance, please contact the Customer Service Centre:

Email: custserv@iec.ch
Tel: +41 22 919 02 11
Fax: +41 22 919 03 00

INTERNATIONAL ELECTROTECHNICAL COMMISSION

CISPR 16-1-5

First edition
2003-11

INTERNATIONAL SPECIAL COMMITTEE ON RADIO INTERFERENCE

Specification for radio disturbance and immunity measuring apparatus and methods –

Part 1-5:

Radio disturbance and immunity measuring apparatus – Antenna calibration test sites for 30 MHz to 1 000 MHz

© IEC 2003 Copyright - all rights reserved

No part of this publication may be reproduced or utilized in any form or by any means, electronic or mechanical, including photocopying and microfilm, without permission in writing from the publisher.

International Electrotechnical Commission, 3, rue de Varembe, PO Box 131, CH-1211 Geneva 20, Switzerland
Telephone: +41 22 919 02 11 Telefax: +41 22 919 03 00 E-mail: inmail@iec.ch Web: www.iec.ch



Commission Electrotechnique Internationale
International Electrotechnical Commission
Международная Электротехническая Комиссия

PRICE CODE

XA

For price, see current catalogue

CONTENTS

FOREWORD	5
INTRODUCTION	9
TABLE RECAPITULATING CROSS REFERENCES	11
1 Scope	13
2 Normative references	13
3 Definitions	15
4 Specifications and validation procedures for a test site to be used to calibrate antennas in the frequency range of 30 MHz to 1 000 MHz	17
4.1 Introduction	17
4.2 Antenna calibration test site (CALTS) specification	19
4.3 Test antenna specification	19
4.4 Antenna calibration test site validation procedure	25
4.5 Antenna calibration test site compliance criteria	35
4.6 The validation report	43
4.7 Validation of the CALTS for vertical polarization	47
Annex A (informative) CALTS requirements	49
Annex B (informative) Test antenna considerations	55
Annex C (informative) Antenna and site attenuation theory	67
Annex D (informative) Application of a fixed length dipole ($30 \text{ MHz} \leq f \leq 80 \text{ MHz}$)	91
Annex E (informative) Pascal Program used in C.1.3	93
Annex F (informative) Checklist validation procedure	101

INTERNATIONAL ELECTROTECHNICAL COMMISSION
INTERNATIONAL SPECIAL COMMITTEE ON RADIO INTERFERENCE

**SPECIFICATION FOR RADIO DISTURBANCE AND IMMUNITY
MEASURING APPARATUS AND METHODS –**

**Part 1-5: Radio disturbance and immunity measuring apparatus –
Antenna calibration test sites for 30 MHz to 1 000 MHz**

FOREWORD

- 1) The International Electrotechnical Commission (IEC) is a worldwide organization for standardization comprising all national electrotechnical committees (IEC National Committees). The object of IEC is to promote international co-operation on all questions concerning standardization in the electrical and electronic fields. To this end and in addition to other activities, IEC publishes International Standards, Technical Specifications, Technical Reports, Publicly Available Specifications (PAS) and Guides (hereafter referred to as "IEC Publication(s)"). Their preparation is entrusted to technical committees; any IEC National Committee interested in the subject dealt with may participate in this preparatory work. International, governmental and non-governmental organizations liaising with the IEC also participate in this preparation. IEC collaborates closely with the International Organization for Standardization (ISO) in accordance with conditions determined by agreement between the two organizations.
- 2) The formal decisions or agreements of IEC on technical matters express, as nearly as possible, an international consensus of opinion on the relevant subjects since each technical committee has representation from all interested IEC National Committees.
- 3) IEC Publications have the form of recommendations for international use and are accepted by IEC National Committees in that sense. While all reasonable efforts are made to ensure that the technical content of IEC Publications is accurate, IEC cannot be held responsible for the way in which they are used or for any misinterpretation by any end user.
- 4) In order to promote international uniformity, IEC National Committees undertake to apply IEC Publications transparently to the maximum extent possible in their national and regional publications. Any divergence between any IEC Publication and the corresponding national or regional publication shall be clearly indicated in the latter.
- 5) IEC provides no marking procedure to indicate its approval and cannot be rendered responsible for any equipment declared to be in conformity with an IEC Publication.
- 6) All users should ensure that they have the latest edition of this publication.
- 7) No liability shall attach to IEC or its directors, employees, servants or agents including individual experts and members of its technical committees and IEC National Committees for any personal injury, property damage or other damage of any nature whatsoever, whether direct or indirect, or for costs (including legal fees) and expenses arising out of the publication, use of, or reliance upon, this IEC Publication or any other IEC Publications.
- 8) Attention is drawn to the Normative references cited in this publication. Use of the referenced publications is indispensable for the correct application of this publication.
- 9) Attention is drawn to the possibility that some of the elements of this IEC Publication may be the subject of patent rights. IEC shall not be held responsible for identifying any or all such patent rights.

International Standard CISPR 16-1-5 has been prepared by CISPR subcommittee A: Radio interference measurements and statistical methods.

This first edition of CISPR 16-1-5, together with CISPR 16-1-1, CISPR 16-1-2, CISPR 16-1-3 and CISPR 16-1-4, cancels and replaces the second edition of CISPR 16-1, published in 1999, amendment 1 (2002) and amendment 2 (2003). It contains the relevant clauses of CISPR 16-1 without technical changes.

This publication has been drafted in accordance with the ISO/IEC Directives, Part 2.

The committee has decided that the contents of this publication will remain unchanged until 2005. At this date, the publication will be

- reconfirmed;
- withdrawn;
- replaced by a revised edition, or
- amended.

IECNORM.COM: Click to view the full PDF of CISPR 16-1-5:2003

Withdrawn

INTRODUCTION

CISPR 16-1, CISPR 16-2, CISPR 16-3 and CISPR 16-4 have been reorganised into 14 parts, to accommodate growth and easier maintenance. The new parts have also been renumbered. See the list given below.

Old CISPR 16 publications		New CISPR 16 publications	
CISPR 16-1	Radio disturbance and immunity measuring apparatus	CISPR 16-1-1	Measuring apparatus
		CISPR 16-1-2	Ancillary equipment – Conducted disturbances
		CISPR 16-1-3	Ancillary equipment – Disturbance power
		CISPR 16-1-4	Ancillary equipment – Radiated disturbances
		CISPR 16-1-5	Antenna calibration test sites for 30 MHz to 1 000 MHz
CISPR 16-2	Methods of measurement of disturbances and immunity	CISPR 16-2-1	Conducted disturbance measurements
		CISPR 16-2-2	Measurement of disturbance power
		CISPR 16-2-3	Radiated disturbance measurements
		CISPR 16-2-4	Immunity measurements
CISPR 16-3	Reports and recommendations of CISPR	CISPR 16-3	CISPR technical reports
		CISPR 16-4-1	Uncertainties in standardised EMC tests
		CISPR 16-4-2	Measurement instrumentation uncertainty
		CISPR 16-4-3	Statistical considerations in the determination of EMC compliance of mass-produced products
CISPR 16-4	Uncertainty in EMC measurements	CISPR 16-4-4	Statistics of complaints and a model for the calculation of limits

More specific information on the relation between the 'old' CISPR 16-1 and the present 'new' CISPR 16-1-5 is given in the table after this introduction (TABLE RECAPITULATING CROSS REFERENCES).

Measurement instrumentation specifications are given in five new parts of CISPR 16-1, while the methods of measurement are covered now in four new parts of CISPR 16-2. Various reports with further information and background on CISPR and radio disturbances in general are given in CISPR 16-3. CISPR 16-4 contains information related to uncertainties, statistics and limit modelling.

CISPR 16-1 consists of the following parts, under the general title *Specification for radio disturbance and immunity measuring apparatus and methods – Radio disturbance and immunity measuring apparatus*:

- Part 1-1: Measuring apparatus,
- Part 1-2: Ancillary equipment – Conducted disturbances,
- Part 1-3: Ancillary equipment – Disturbance power,
- Part 1-4: Ancillary equipment – Radiated disturbances,
- Part 1-5: Antenna calibration test sites for 30 MHz to 1 000 MHz.

TABLE RECAPITULATING CROSS REFERENCES

Second edition of CISPR 16-1
Clauses, subclauses

First edition of CISPR 16-1-5
Clauses, subclauses

1
2
3
5.13

1
2
3
4

Annexes

R
S
T
U
V
W

Annexes

A
B
C
D
E
F

Figures

55, 56, 57, 58, 59
S.1, S.2, S.3, S.4
T.1, T.2, T.3

Figures

1, 2, 3, 4, 5
B.1, B.2, B.3, B.4
C.1, C.2, C.3

Tables

19, 20

Tables

1, 2

SPECIFICATION FOR RADIO DISTURBANCE AND IMMUNITY MEASURING APPARATUS AND METHODS –

Part 1-5: Radio disturbance and immunity measuring apparatus – Antenna calibration test sites for 30 MHz to 1 000 MHz

1 Scope

This part of CISPR 16 is designated a basic standard which specifies the requirements for calibration test sites, used to perform antenna calibrations, as well as the test antenna characteristics, calibration site verification procedure and site compliance criteria. Further information on calibration site requirements, test antenna considerations and the theory of antennas and site attenuation is provided in informative annexes.

Measurement instrumentation specifications are given in CISPR 16-1-1 and CISPR 16-1-4. Further information and background on uncertainties in general is given in CISPR 16-4-1, which may be helpful in establishing uncertainty estimates for the calibration processes of antennas.

2 Normative references

The following referenced documents are indispensable for the application of this document. For dated references, only the edition cited applies. For undated references, the latest edition of the referenced document (including any amendments) applies.

CISPR 14-1:2000, *Electromagnetic compatibility – Requirements for household appliances, electric tools and similar apparatus – Part 1: Emission*

CISPR 16-1-1:2003, *Specification for radio disturbance and immunity measuring apparatus and methods – Part 1-1: Radio disturbance and immunity measuring apparatus – Measuring apparatus*

CISPR 16-1-4:2003, *Specification for radio disturbance and immunity measuring apparatus and methods – Part 1-4: Radio disturbance and immunity measuring apparatus – Ancillary equipment – Radiated disturbances*

CISPR 16-4-1:2003, *Specification for radio disturbance and immunity measuring apparatus and methods – Part 4-1: Uncertainties, statistics and limit modelling – Uncertainties in standardised EMC tests*

CISPR 16-4-2:2003, *Specification for radio disturbance and immunity measuring apparatus and methods – Part 4-2: Uncertainties, statistics and limit modelling – Measurement instrumentation uncertainties*

IEC 60050(161):1990, *International Electrotechnical Vocabulary (IEV) – Chapter 161: Electromagnetic compatibility*

International Vocabulary of Basic and General Terms in Metrology, International Organization for Standardization, Geneva, 2nd edition, 1993

3 Definitions

For the purpose of this section of CISPR 16, the following definitions apply. Also see IEC 60050(161).

3.1

calibration test site (CALTS)

open area test site with metallic ground plane and tightly specified site attenuation performance in horizontal and vertical electric field polarization

A CALTS is used for determining the free-space antenna factor of an antenna.

Site attenuation measurements of a CALTS are used for comparison to corresponding site attenuation measurements of a compliance test site, in order to evaluate the performance of the compliance test site

3.2

compliance test site (COMTS)

environment which assures valid, repeatable measurement results of disturbance field strength from equipment under test for comparison to a compliance limit

3.3

antenna

that part of a transmitting or receiving system that is designed to radiate or to receive electromagnetic waves in a specified way

NOTE 1 In the context of this standard, the balun is a part of the antenna.

NOTE 2 See also the term "wire antenna".

3.4

balun

passive electrical network for the transformation from a balanced to an unbalanced transmission line or device or vice versa

3.5

free-space-resonant dipole

wire antenna consisting of two straight colinear conductors of equal length, placed end to end, separated by a small gap, with each conductor approximately a quarter-wavelength long such that at the specified frequency the input impedance of the wire antenna measured across the gap is pure real when the dipole is located in the free space

NOTE 1 In the context of this standard, this wire antenna connected to the balun is also called the "test antenna".

NOTE 2 This wire antenna is also referred to as "tuned dipole".

3.6

site attenuation

site attenuation between two specified positions on a test site is the insertion loss determined by a two-port measurement, when a direct electrical connection between the generator output and receiver input is replaced by transmitting and receiving antennae placed at the specified positions

3.7

test antenna

combination of the free-space-resonant dipole and the specified balun

NOTE For the purpose of this standard only.

3.8

wire antenna

a specified structure consisting of one or more metallic wires or rods for radiating or receiving electromagnetic waves

NOTE A wire antenna does not contain a balun.

4 Specifications and validation procedures for a test site to be used to calibrate antennas in the frequency range of 30 MHz to 1 000 MHz

Clause 5 of CISPR 16-1-4 specifies the requirements for a test site used to make radio disturbance field strength measurements in the frequency range of 30 MHz to 1 000 MHz. Such a test site may not be suitable for calibrating antennas. This clause specifies the requirements and validation procedure for a test site suitable for the calibration of antennas above a conducting, flat metal plane in the frequency range of 30 MHz to 1 000 MHz. A test site meeting these stringent requirements may also be used as a reference test site for comparison purposes in an alternative validation procedure to 5.6 of CISPR 16-1-4.

4.1 Introduction

A test site suitable for performing antenna calibration, referred to herein as CALTS, is intended to provide a suitable environment to calibrate an antenna for its free-space antenna factor. This calibration is performed most conveniently above a reflecting plane by using only horizontal polarization. Subclauses 4.3 through 4.6 specify the characteristics of a CALTS, the characteristics of a calculable test antenna and the CALTS verification (validation) procedure and performance criteria. The CALTS validation procedure given in 4.5 requires the use of a calculable dipole antenna as specified in 4.4, thus creating the possibility of comparing theoretically predicted site-attenuation to measured CALTS performance. Items to be reported in a CALTS validation report are summarized in 4.7. Annex A provides guidance for constructing a CALTS, which complies with validation criteria specified in 4.6.

In order for a CALTS to be used as a reference test site (REFSITE) for validating the performance of test sites according to clause 5 of CISPR 16-1-4, some additional requirements need to be specified. Subclause 4.7 specifies the additional characteristics and performance criteria. Test sites specified in clause 5 of CISPR 16-1-4, which are used for demonstrating compliance with radiated emission limits are referred to herein as a compliance test site (COMTS). Validation of a COMTS may be obtained by comparing it to the theoretical site attenuation given in clause 5 of CISPR 16-1-4 (which takes precedence) or by comparing site attenuation measurements of the REFSITE to corresponding site attenuation measurements of the COMTS, using the same measurement set-up and equipment (antennas, cables, generator, receiver, etc.).

The annexes to this standard contain informative specifications of a CALTS and of the calculable, free-space-resonant dipole (tuned dipole) to be used in the CALTS validation procedures. They also give a model for calculating theoretical site attenuation, numerical examples and a checklist for the validation procedure.

4.2 Antenna calibration test site (CALTS) specification

4.2.1 Introduction

The CALTS comprises the following main components:

- a good-conducting flat metal plane (the reflecting plane);
- an electromagnetically obstruction-free area surrounding the reflecting plane.

In addition, the following ancillary equipment is needed:

- two antenna masts carrying the antennas to be used in either the CALTS validation procedure or the antenna calibration procedure;
- the cables to be connected to these antennas; and
- electronic equipment, such as an RF generator and a measuring receiver.

The normative specification for a CALTS is given in 4.2.2, while annex A contains a number of informative specifications as a guidance to construct and place a CALTS in such a way that the validation criteria will normally be met.

4.2.2 Normative specification

For the calibration of antennas, the CALTS shall comply with the validation criteria given in 4.5.3, i.e.

- a) site attenuation at fixed antenna heights, and
- b) antenna heights for maximum site attenuation, or for maximum site attenuation, at all frequencies at which the antennas shall be calibrated.

NOTE 1 In the CALTS validation procedure, equipment is used which is also subject to normative specifications (see 4.3 and 4.4).

NOTE 2 The CALTS validation report (4.6) will contain information on how compliance with the requirements is maintained, so that the CALTS is deemed to comply with the requirements during its actual use.

4.3 Test antenna specification

4.3.1 Introduction

To allow (numerical) calculation of the theoretical site attenuation SA_c needed in the validation procedure, antennas are needed which can be accurately modelled. Therefore, the test antenna shall be a free-space resonant dipole connected to a balun with specified properties. The normative test antenna specifications are given in 4.3.2. An example of the construction of a test antenna is given in annex B.

The test antenna consists of a balun and two colinear wire elements (conductors) each having a diameter D_{we} and length L_{we} . These elements are connected to the two feed terminals (A and B in figure 1) at the balun. The gap between these feed terminals has a width W_g . The tip-to-tip length L_a of the antenna is given by $L_a = 2L_{we} + W_g$. The centre of the test antenna is in the middle of the feed-terminal gap on the centre-line of the two colinear wire elements.

The balun has an unbalanced input/output (transmitting/receiving antenna) port and a balanced port at the two feed terminals A and B. As an example, in figure 1 the purpose of the balun is indicated schematically by the balance/unbalance transformer.

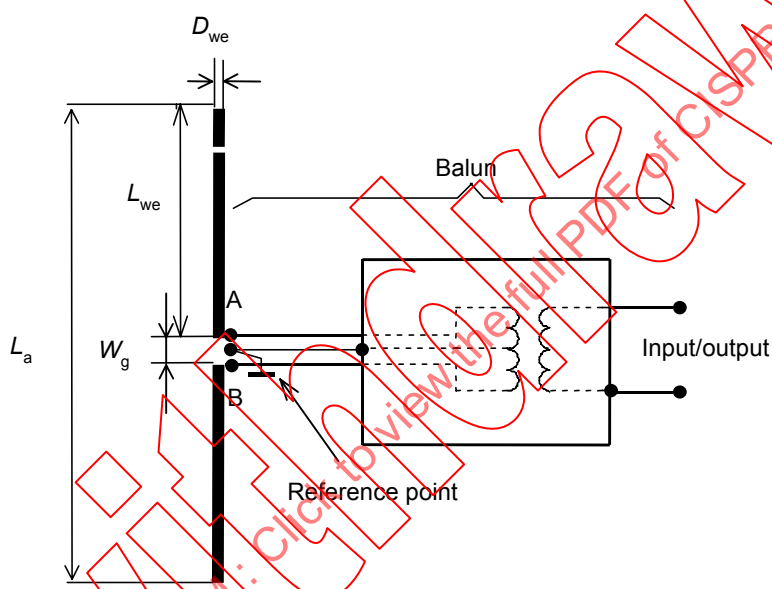
4.3.2 Normative specifications

4.3.2.1 The test antenna shall have identical wire elements of length L_{we} which can be disconnected from the balun to enable the balun parameters to be validated, and to allow the balun heads of the two antennas used in site attenuation measurements to be connected together.

4.3.2.2 The tip-to-tip length $L_a(f, D_{we})$ of the approximately $\lambda/2$ wire antenna is determined by the condition that, at the specified frequency f and in free space, the absolute value of the imaginary part of the input impedance at the feed terminals is smaller than 1Ω .

NOTE 1 If the wire elements have a constant diameter and if $D_{we} \ll L_a$, then $L_a(f, D_{we})$ can be calculated from the equation (C.2) in subclause C.1.1. If the diameter is not a constant, e.g. when a telescopic antenna is used, $L_a(f)$ can only be calculated numerically, see C.2.2.

NOTE 2 When using a telescopic antenna, the telescopic elements should be tuned in such a way that the elements having the largest diameter are used first (see figure 2), and the numerical calculations should account for this approach.



IEC 843/99

NOTE – The centre of the test antenna is in the middle of the gap on the centre-line of the two wire elements.

Figure 1 – Schematic diagram of the test antenna

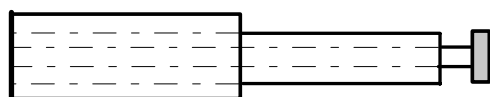


Figure 2a – Correct IEC 844/99

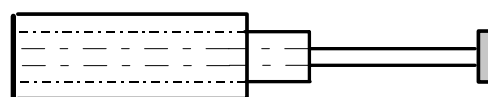


Figure 2b – Incorrect IEC 845/99

Figure 2 – Adjustment of a telescopic wire element to the length L_{we}

Under consideration: At test frequencies between 30 MHz and 80 MHz, a fixed length dipole with $L_a = L_a$ (80 MHz) may be used.

4.3.2.3 The feed-terminal gap shall be $W_g \leq 15 \text{ mm}$ or $W_g \leq 0,03 \lambda_{\min}$, whichever is the smaller,

where

$$\lambda_{\min} = c_0/f_{\max},$$

$f_{\max}$ is the highest test frequency at which the test antenna is used; and

c_0 is the velocity of the electromagnetic waves in vacuum.

4.3.2.4 If the tip-to-tip length $L_a(f)$ of the actual wire antenna is within ΔL_a of the length $L_a(f)$ specified for that antenna (see table 2), that length is presumed to be validated when the width of the feed-terminal gap complies with 4.3.2.3.

4.3.2.5 The balanced port of the balun shall have:

- a specified impedance Z_{AB} with a specified maximum VSWR, see table 2, when the unbalanced port is terminated in the impedance Z_e presented to it by the external circuitry (the antenna feed cable);
- an amplitude balance with respect to the balun reference point better than ΔA_b dB, see table 2, when both feed terminals are terminated in an impedance $Z_{AB}/2$ with respect to the balun reference point;
- a phase balance of $180^\circ \pm \Delta \phi_b$ (see table 2), when both feed terminals are terminated in an impedance $Z_{AB}/2$ with respect to the balun reference point.

NOTE 1 Connectors at the balun ports should enable RF measurements to be made at the three balun ports.

NOTE 2 The balanced port impedance Z_{AB} is the impedance between the feed terminals A and B in figure 1. The preferred value of this impedance is $Z_{AB} = 100 \Omega$ (real).

NOTE 3 The impedance Z_e presented by the external circuitry is usually 50Ω , being the preferred value.

NOTE 4 The amplitude and phase balance requirements ensure that the signals at the feed terminals A and B are sufficiently equal in amplitude and opposite in phase with respect to the balun reference point. When the balanced port meets these requirements, the isolation between the two feed terminals will be more than 26 dB when the unbalanced port is terminated in the impedance Z_e .

NOTE 5 As far as practical, the balun components should be oriented to present the minimum co-polarized reflecting surface to the wire antenna.

NOTE 6 The components of the balun are electrically screened, so that their (parasitic) properties cannot be influenced by the surroundings. The balun reference point and the ground terminal of the output/input port are connected to that screen.

4.3.2.6 The balun properties required in 4.3.2.5 may be determined from S-parameter measurements and, partly, from injection measurements.

NOTE 1 The head-to-head connection of the baluns in 4.4.4.2 and 4.4.4.4 may be replaced by a cable-to-cable connection when the full set of balun S-parameters and the port impedances presented to the baluns by the generator and the receiver are known, provided the balun properties are incorporated in the SA_c calculation.

NOTE 2 S-parameter and injection measurements are described in annex B.

4.3.2.7 If, in the CALTS validation procedure, test antennas and/or test equipment is used with Z_{AB} and/or Z_e differing from the preferred values 100 Ω and 50 Ω , respectively, then this should be explicitly mentioned in the validation report (4.6).

4.4 Antenna calibration test site validation procedure

4.4.1 Introduction

In the validation procedure, the measured site attenuation SA_m is compared with the theoretically calculated site attenuation SA_c . The procedure thus verifies whether the CALTS sufficiently meets the properties assumed in the SA calculations, i.e.:

- a) the plane is perfectly flat and infinitely large;
- b) the absolute value of the reflection coefficient of that plane is $r = 1$, and
- c) the phase difference of the incoming and reflected horizontally polarized EM waves at the plane is $\phi = \pi$ radians;
- d) the influence of the ancillary equipment and surroundings of the plane is negligible.

To verify the properties, two sets of measurements are required:

- 1) the properties a), b) and d) are verified simultaneously in a SA measurement procedure using fixed antenna heights (see 4.4.4), after which the measured and calculated SA are compared;
- 2) the properties a), c) and d) are verified simultaneously in a procedure in which the height of one of the test antennas is scanned for maximum SA after which the measured and calculated height of that antenna corresponding with that maximum are compared (see 4.4.5).

Alternatively, the latter set of properties may also be verified simultaneously in a scanned frequency measurement procedure (see 4.4.6).

Below, a quantity $\pm \Delta X$ represents the maximum tolerance of a parameter value X allowed in the validation procedure. The quantitative data for the tolerances are summarized in table 2.

4.4.2 Test set-up

4.4.2.1 The centres of the test antennas, the antenna masts and the antenna coaxial antenna cables are positioned in a plane perpendicular to the reflecting plane and centrally located on the reflecting plane.

NOTE The centre of the test antenna has been defined in 4.3.1

4.4.2.2 The colinear wire elements are positioned parallel to the reflecting plane (antenna in horizontal polarization) throughout, and perpendicular to the (vertical) plane mentioned in 4.4.2.1.

NOTE At the lower end of the frequency range, e.g. 30 MHz to 40 MHz, the relatively long wire elements may droop, thus influencing the measuring results. This influence can be eliminated by physically propping up the wire elements, or can be accounted for in the calculation of the theoretical site attenuation (see also 4.4.4.3 and 4.5.3.1).

4.4.2.3 The horizontal distance between the centres of the test antennas is

$$d = 10,00 \text{ m} \pm \Delta d \text{ m (see table 2).}$$

4.4.2.4 The height of the centre of the transmitting antenna above the reflecting plane is

$$h_t = 2,00 \text{ m} \pm \Delta h_t \text{ m (see table 2).}$$

4.4.2.5 The height of the centre of the receiving antenna above the reflecting plane shall be adjustable to the heights $h_r \pm \Delta h_r$, as specified in table 1 and table 2, and shall be scannable over the height range $1,0 \text{ m} \leq h_r \leq 4,0 \text{ m}$ as required in 4.4.5.

4.4.2.6 The coaxial cables connected to the baluns of the transmitting and receiving antennas run perpendicular to the wire elements and parallel to the reflecting plane over a distance of at least 1 m from the wire elements. After that, the cables may drop onto the reflecting plane and (preferably) continue to run underneath the reflecting plane or on top of that plane perpendicularly to the wire elements until they reach the edge of the plane. To avoid common mode coupling, ferrite loading of the coaxial cables connected to the baluns is advised.

NOTE 1 The cables should have a low transfer impedance to avoid influence on the measured results of the induced cable sheet currents through that impedance.

NOTE 2 When the cables run partly underneath the reflecting plane, the sheath of the cable should be bonded (360° around) to the reflecting plane when penetrating that plane.

4.4.2.7 The RF generator and RF receiver shall not be elevated above the level of the reflecting plane if they are within 20 m from the plane.

4.4.2.8 The RF generator shall have a good frequency and output level stability throughout the duration of the site-attenuation measurements. See also 4.4.4.5.

NOTE It might be necessary to include a warm-up time (normally indicated by the equipment manufacturer) of the RF generator and RF receiver in the measuring procedure, to assure a sufficient long-term stability of these equipments.

4.4.2.9 The RF receiver shall have its linearity calibrated over a dynamic range of at least 50 dB. The uncertainty of the receiver linearity is denoted as ΔA_r (see 4.5.2.2). A reasonable value for the receiver linearity uncertainty is 0,2 dB.

NOTE If the linear dynamic range is less than 50 dB a substitution method may be followed, using a calibrated precision attenuator as described in 4.4.4.7.

4.4.3 Test frequencies and receiving antenna heights

4.4.3.1 With due observance to 4.2.2, the validation measurements described in 4.4.4 shall be carried out at least at the frequencies and the associated fixed heights of the centre of the receiving antenna h_r (m) above the reflecting plane given in table 1.

NOTE 1 Information concerning the CALTS performance at the intermediate frequencies can be obtained by using swept-frequency measurements as described in A.2.2.

NOTE 2 Care shall be taken in case of high-Q responses, especially for frequencies above 300 MHz. In such a case a swept-frequency procedure should be carried out around the specified frequencies and at the associated heights.

4.4.3.2 In addition to the validation measurements described in 4.4.4, either three receiving antenna height-scan measurements as described in 4.4.5 or three frequency-scan measurements as described in 4.4.6 shall be carried out.

- a) When choosing to perform receiving-antenna, height-scan measurements, these shall be carried out at the frequencies f_s : 300 MHz, 600 MHz and 900 MHz, with the test antennas tuned to the associated frequency f_s .

- b) When choosing to perform frequency-scan measurements, these shall be carried out with combinations $\{h_{rs}, f_s\}$: {2,65 m, 300 MHz}, {1,30 m, 600 MHz} and {1,70 m, 900 MHz} of the receiving antenna height h_{rs} and the test antenna tuned frequency f_s .

Table 1 – Frequency and fixed receiving antenna height data for SA measurements where $h_t = 2$ m and $d = 10$ m (4.4.2.3 and 4.4.2.4)

Frequency MHz	h_r m	Frequency MHz	h_r m	Frequency MHz	h_r m
30	4,00	90	4,00	300	1,50
35	4,00	100	4,00	400	1,20
40	4,00	120	4,00	500	2,30
45	4,00	140	2,00	600	2,00
50	4,00	160	2,00	700	1,70
60	4,00	180	2,00	800	1,50
70	4,00	200	2,00	900	1,30
80	4,00	250	1,50	1 000	1,20

4.4.3.3 If narrow-band noise, such as that originating from broadcast transmitters, hinders accurate measurement at a frequency specified in 4.4.3.1 and 4.4.3.2, a usable test frequency as close as possible to that specified frequency shall be chosen.

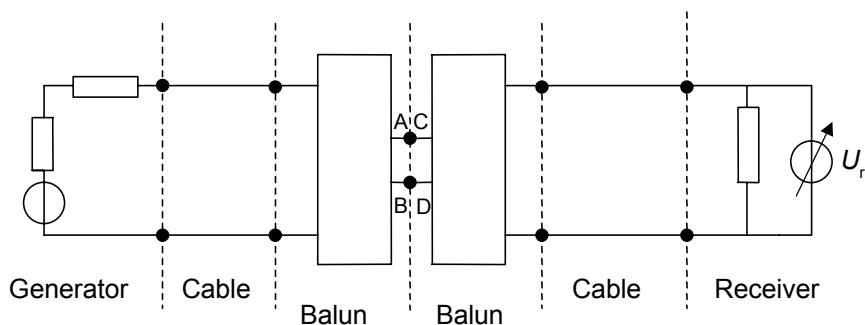
The rationale for a deviation from a specified frequency shall be recorded in the validation report (see 4.6).

4.4.3.4 The frequency of the RF generator providing the signal for the transmitting antenna shall be adjusted to within Δf (see table 2), of a test frequency specified in table 1 or in 4.4.3.2.

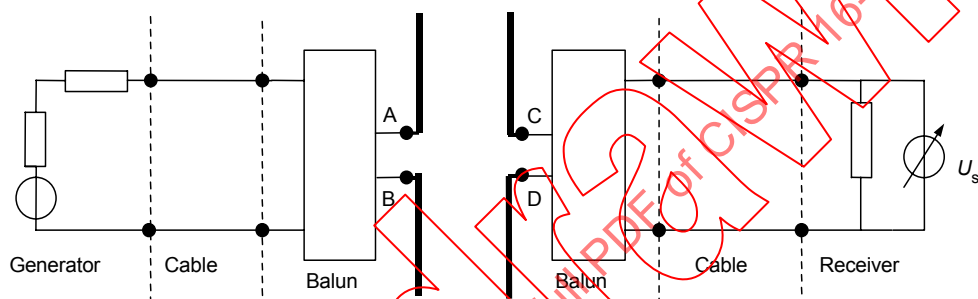
4.4.4 Site attenuation measurements

This subclause describes the three measurements needed to determine the measured site attenuation SA_m (see 4.5.3.1), at the specified frequencies. The site attenuation being considered is the SA between the feed terminals of the transmitting antenna (A and B in figures 3 and 4) and those of the receiving antenna (C and D in figures 3 and 4).

NOTE Where a full set of balun S-parameters is available (see 4.3.2.6), it is also possible to consider the SA between the two cable/balun interfaces provided the balun properties are incorporated in the calculation of the theoretical SA. In the description given below, the latter possibility will be indicated by a note, where appropriate.



IEC 846/99

Figure 3 – Determination $U_{r1}(f)$ or $U_{r2}(f)$ 

IEC 847/99

Figure 4 – Determination $U_s(f)$ with the wire antennas in their specified position

4.4.4.1 Measurement 1: At a specified frequency f , the reference voltage $U_{r1}(f)$ is determined. This voltage makes it possible to account for the attenuation of the signal between the RF generator output port and the feed terminals of the transmitting wire antenna and, similarly, between the feed terminals of the receiving wire antenna and the receiver input port.

$U_{r1}(f)$ is determined as follows (see figure 3). The wire elements of the test antennas are disconnected from their balun and the two baluns are connected head-to-head (see also note 4 below) with a connection which is as short as possible, preferably $< \lambda_{\min}/10$, where $\lambda_{\min}$ has been defined in 4.3.2.3.

The level of the RF generator is set to give a receiver reading at least 60 dB above the noise level of the receiver (see note 2 below). The receiver reading is recorded as $U_{r1}(f)$.

NOTE 1 The level of the emitted field should not exceed the local transmission permitted levels.

NOTE 2 In this subclause it is presumed that the RF receiver complies with 4.4.2.9. Where the note to 4.4.2.9 applies, the method given in 4.4.4.7 should be applied.

NOTE 3 The noise level of the receiver can be reduced by reducing the receiver bandwidth. However, if the RF generator and RF receiver are not frequency-locked, as in the case of a tracking generator and spectrum analyser, the receiver bandwidth should be sufficiently wide that a possible drift of the frequency of the RF generator signal does not influence the measuring results.

NOTE 4 If the method given in the note to 4.4.4 is followed, the complete test antennas are disconnected and the two antenna cables are interconnected when determining $U_{r1}(f)$ and $U_{r2}(f)$ in 4.4.4.4.

4.4.4.2 The amplitude setting of the RF generator used in 4.4.4.1 at a particular frequency remains unchanged throughout the measurements associated with 4.4.4.3 and 4.4.4.4.

4.4.4.3 Measurement 2: The baluns are disconnected from each other, the wire elements connected to their balun (see figure 4), and are adjusted to the specified length $L_a(f)$. The test antennas are brought into position as specified in 4.4.2 and 4.4.3. All other elements in the test set-up are the same as in 4.4.4.1. See also the notes to 4.4.2.2 and 4.4.4.5.

At the specified test frequency f , and with the antennas in their specified position, the receiver reading is recorded as $U_s(f)$.

4.4.4.4 Measurement 3: The measurement of the reference voltage (see 4.4.4.1), is repeated at the same specified frequency. The value is recorded as $U_{r2}(f)$.

4.4.4.5 If $U_{r1}(f)$ and $U_{r2}(f)$, expressed in logarithmic units, differ by more than 0,2 dB, the stability of the test set-up shall be improved and the aforementioned measurements 1, 2 and 3 repeated.

NOTE A cause of instability effects may also be the temperature dependence of the coaxial cable attenuation, especially under direct sunlight exposure.

4.4.4.6 The measured site attenuation $SA_m(f)$ is given by the following equation:

$$SA_m(f) = 20 \log_{10} \left\{ \frac{U_{ra}(f)}{U_s(f)} \right\} \quad (\text{dB}) \quad (1)$$

where $U_{ra}(f)$ is the average of $U_{r1}(f)$ and $U_{r2}(f)$.

NOTE If no provisions have been taken to avoid the droop of the wire elements of both test antennas at the lower frequencies 30 MHz, 35 MHz and 40 MHz, it might be necessary to correct the measured site attenuation SA_m (see 4.5.3.1).

4.4.4.7 Where the dynamic range of the RF receiver does not comply with 4.4.2.9, the following substitution method may be used provided the full set of balun S-parameters is available and the balun properties are incorporated in the calculation of the theoretical SA.

- Determine and record the receiver reading $U_s(f)$ as described in 4.4.4.3.
- Replace the test antennas by a calibrated precision attenuator and connect both antenna cables to this attenuator. Adjust the insertion loss caused by the attenuator to a level $A_{i1}(f)$ such that the same receiver reading $U_s(f)$ as determined under a) is found. Record $A_{i1}(f)$ and its associated measurement uncertainty $\Delta A_{i1}(f)$.
- To demonstrate the stability of the test set-up mentioned in 4.4.2.8, repeat step b) to determine $A_{i2}(f)$ after a period of time approximating the total time between the reading of $U_s(f)$ in step a) and $A_{i1}(f)$ in step b). If $A_{i2}(f)$ differs by more than 0,2 dB from $A_{i1}(f)$, the stability of the test set-up shall be improved and steps a), b) and c) repeated.
- If the test set-up is sufficiently stable, the measured site attenuation is given by

$$SA_m(f) = 20 \log_{10} \{A_{ia}\} \quad (\text{dB}) \quad (2)$$

where $A_{ia}(f)$ is the average value of $A_{i1}(f)$ and $A_{i2}(f)$ in linear units.

4.4.5 Antenna-height scan measurements

This subclause describes the three antenna-height scan measurements needed to determine the receiving antenna height $h_{r,max}$ at which the measured site attenuation shows a sharp maximum (see 4.4.3.2a) and 4.5.3.2). The sharp maximum results from (near-total) cancellation of the direct wave arriving at the receiving antenna by the indirect wave, i.e. the wave reflected from the reflecting plane.

4.4.5.1 At the frequencies f_s , specified in 4.4.3.2a) and in the test set-up as described in 4.4.2 the height of the receiving test antenna (tuned to the frequency f_s) is increased from a height $h_r = 1,0$ m up to a height $h_{r,max}(f_s)$ corresponding with the first sharp maximum in the SA, i.e. the first sharp minimum in the receiver reading.

NOTE The value of the minimum in the receiver reading is not of interest. This reading is only an indicator to find $h_{r,max}(f_s)$.

4.4.5.2 The height $h_{r,max}(f_s)$ is measured and recorded together with its associated measurement uncertainty $\Delta h_{r,max}(f_s)$.

NOTE The measured $h_{r,max}(f_s)$ may not be equal to $h_{rs}(f_s)$ as given in 4.4.3.2 b) because $h_{r,max}(f_s)$ depends on the properties of the actual test antennas as well.

4.4.6 Frequency scan measurements

This subclause describes the three swept frequency measurements needed to determine the frequency f_{max} at which the measured site attenuation shows a sharp maximum, see 4.4.3.2b) and 4.5.3.3). The sharp maximum results from (near-total) cancellation of the direct wave arriving at the receiving antenna by the indirect wave, i.e. the wave reflected from the reflecting plane.

4.4.6.1 At the fixed receiving test antenna heights, $h_{rs}(f_s)$ specified in 4.4.3.2 b) and in the test set-up with the test antennas tuned to the associated frequency f_s as given in 4.4.3.2 b), the frequency of the RF generator is scanned from a frequency well below f_s , say 100 MHz lower than f_s , up to a value $f_{max}(h_{rs})$ corresponding with a full sharp maximum in the SA, i.e. minimum in the receiver reading.

NOTE The value of the minimum in the receiver reading is not of interest. This reading is only an indicator to find $f_{max}(h_{rs})$.

4.4.6.2 The frequency $f_{max}(h_{rs})$ is recorded together with its associated measuring uncertainty, $\Delta f_{max}(h_{rs})$.

NOTE The measured $f_{max}(h_{rs})$ need not be equal to $f_s(h_{rs})$ as given in 4.4.3.2 a) because $f_{max}(h_{rs})$ depends on the properties of the actual test antennas as well.

4.5 Antenna calibration test site compliance criteria

4.5.1 Introduction

The CALTS is deemed to be satisfactory when, at all frequencies at which antenna calibrations requiring a CALTS are to be performed, the measured site attenuation (4.4.3.1) and the measured antenna heights or the measured frequency (4.4.3.2) are within a certain margin of the calculated theoretical values (4.5.3). Apart from the uncertainties in the various measurement data, this margin also takes into account the tolerances allowed in the measurement set-up.

As explained in 4.5.2, the uncertainty margin consists of a part which shall be calculated using the theoretical model and a part which is directly coupled to the uncertainty in the voltage measurements from which the measured site attenuation is determined, and to uncertainties in the scanned height or swept frequency measurements.

4.5.2 Tolerances and measurement uncertainties

4.5.2.1 The maximum tolerances for the various parameters are listed in table 2.

Table 2 – Maximum tolerances for $d = 10$ m

Variable	Maximum tolerance	Subclause
L_a	$\pm 0,0025 L_a$ or $\pm 0,001$ (m) if $L_a < 0,400$ (m)	4.3.2.4
Z_{AB}	$VSWR \leq 1,10$	4.3.2.5 a)
A_b	$\pm 0,4$ dB	4.3.2.5 b)
ϕ_b	$\pm 2^\circ$	4.3.2.5 c)
d	$\pm 0,04$ m	4.4.2.3
h_t	$\pm 0,01$ m	4.4.2.4
h_r	$\pm 0,01$ m	4.4.2.5
f	$\pm 0,001f$	4.4.3.4
NOTE The need to take into account the tolerance ΔD_{we} in the radius of a wire element and the uncertainties associated with the alignment of the wire antennas, is under consideration.		

4.5.2.2 The measurement uncertainty ΔSA_m in the measured site attenuation SA_m as defined in equation (1) in 4.4.4.6 is given by

$$\Delta SA_m(\text{dB}) = \sqrt{\{\Delta SA_r(\text{dB})\}^2 + \{\Delta SA_t(\text{dB})\}^2} \quad (3)$$

where ΔSA_r is given by ΔA_r in 4.4.2.9, or by $\Delta A_i(f)$ in 4.4.4.7, whichever subclause is applicable. ΔSA_t accounts for the sensitivity of the site attenuation to the parameter tolerances (maximum values as given in table 2). The 95 % confidence level values of ΔSA_r and ΔSA_t shall be used in equation (3).

NOTE ΔSA_t (95 %) may be calculated using the model given in annex C.

4.5.2.3 If the tolerances of the parameters comply with those given in table 2, ΔSA_t (95 %) = 0,2 dB may be used for the whole frequency range from 30 MHz to 1 000 MHz. In that case, it is not needed to perform ΔSA_t calculations nor to report the results of the calculations in the CALTS validation report.

NOTE A rationale for ΔSA_t (95 %) = 0,2 dB is given in C.1.3.2.

4.5.2.4 The measurement uncertainty Δh_{rm} in the measured height of the receiving antenna $h_{r,\max}$ as defined in 4.4.5, is given by

$$\Delta h_{rm}(\text{m}) = \sqrt{\{\Delta h_{r,\max}(\text{m})\}^2 + \{\Delta h_{rt}(\text{m})\}^2} \quad (4)$$

where $\Delta h_{r,\max}$ is defined in 4.4.5.2, and Δh_{rt} accounts for the sensitivity of $h_{r,\max}$ to the parameter tolerances (maximum values as given in table 2).

NOTE Δh_{rt} can be calculated using the model given in C.1.3.3.

4.5.2.5 If the tolerances of the parameters comply with those given in table 2, Δh_{rt} (95 %) = 0,025 m may be used at the three specified frequencies. In that case, it is not needed to perform Δh_{rt} calculations nor to report the results of the calculations in the CALTS validation report.

NOTE A rationale for Δh_{rt} (95 %) = 0,025 m is given in C.1.3.3.

4.5.2.6 The measurement uncertainty Δf_m at the measured frequency $f_{\max}$ as defined in 4.4.6, is given by

$$\Delta f_m (\text{MHz}) = \sqrt{\{\Delta f_{\max} (\text{MHz})\}^2 + \{\Delta f_t (\text{MHz})\}^2} \quad (5)$$

where

$\Delta f_{\max}$ is defined in 4.4.6.2; and

Δf_t accounts for the sensitivity of $f_{\max}$ to the parameter tolerances (maximum values as given in table 2).

NOTE Δf_t can be calculated using the model given in C.1.3.4.

4.5.2.7 If the tolerances of the parameters comply with those given in table 2, Δf_t (95 %)/ f_c = 0,015 may be used at the three specified receiving antenna heights. In that case, it is not needed to perform Δf_t calculations nor to report the results of the calculations in the CALTS validation report.

NOTE A rationale for Δf_t (95 %)/ f_c = 0,015 is given in C.1.3.4.

4.5.3 Compliance criteria

In this subclause, the parameter values to be used in the calculations are the actual values realized in a measurement. The actual parameter values are assumed to be determined with a sufficiently small measurement uncertainty so that the conclusion that a parameter value is within the maximum tolerance range as given in table 2 is justifiable.

EXAMPLE – If the specified distance between the antenna centres d = 10,00 m (4.4.2.3) and during the actual SA measurements that distance equals d_a = 10,01 m, the latter value is used in the calculations. However $(d - d_a)$ shall always be smaller than 0,04 m (see table 2), while d_a has been determined with such a small measurement uncertainty that $|d - d_a| < 0,04$ m is justifiable.

4.5.3.1 The CALTS complies with the site attenuation validation criterion if, at all frequencies used for antenna calibration (figure 5)

$$|SA_c(\text{dB}) - SA_m(\text{dB})| < T_{SA}(\text{dB}) - \Delta SA_m(\text{dB}) \quad (6)$$

where

$SA_c(f)$ is the theoretical SA at the specified frequency, calculated as depicted in annex C, using the test antenna data following after the application of 4.3.2.6 and using the actual geometrical parameter values L_a , d , h_t and h_r ;

$SA_m(f)$ is the measured SA following from equation (1) or equation (2) (see also the note);

$\Delta SA_m(f)$ is the SA measurement uncertainty (95 % confidence level) as derived in 4.5.2.2;

$T_{SA}(f)$ is the allowed tolerance in SA.

Unless stated otherwise in the antenna calibration standard requiring the use of a CALTS, the allowed tolerance is $T_{SA}(f) = 1,0$ dB over the whole frequency range 30 MHz to 1 000 MHz.

As a minimum, it shall be demonstrated that the CALTS complies with the SA criterion at the frequencies listed in table 1.

NOTE 1 At the frequencies 30 MHz to 40 MHz, the value of SA_m needs to be corrected when there is a significant droop at the tip of the wire antenna.

a) At 30 MHz a 4,8 m long dipole droops by 16 cm at the tips. SA_m should be increased by 0,27 dB, 0,13 dB and 0,08 dB when the dipole is at heights of 1 m, 2 m and 4 m respectively, in order to properly compare SA_m with SA_c .

b) If the droop at the tip is larger than 20 cm, the increase of $SA_m(f)$ should be calculated numerically (see clause C.2).

NOTE 2 EXAMPLE

If ΔSA_t (95 %) = 0,2 dB (application of 4.5.2.3) and ΔSA_r (95 %) = 0,2 dB, then ΔSA_m (95 %) = 0,3 dB. Consequently, 0,7 dB is the maximum acceptable difference between calculated and measured site attenuation. The maximum acceptable difference can be increased by using a receiver with a lower value of ΔSA_r (95 %), by decreasing the tolerances of the various parameters and by considering the actual value of ΔSA_t (95 %).

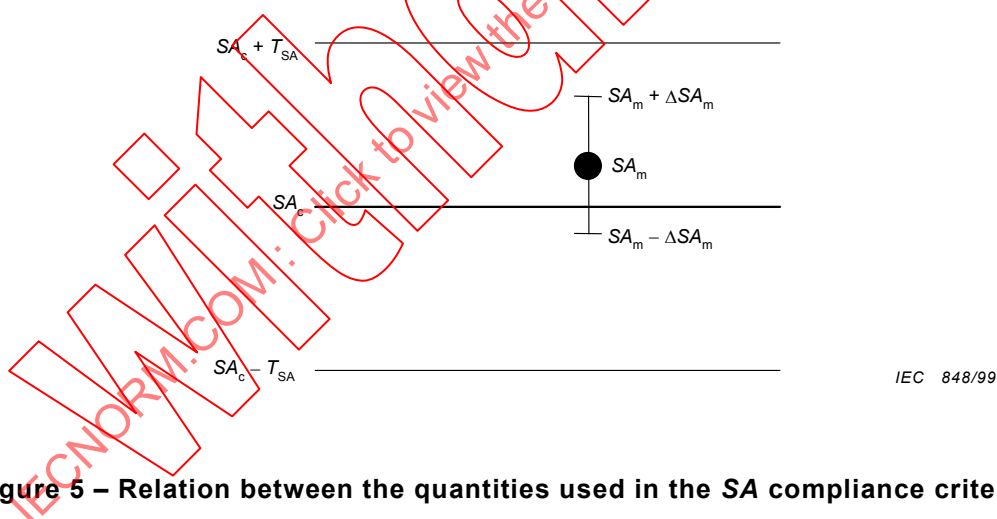


Figure 5 – Relation between the quantities used in the SA compliance criterion

4.5.3.2 The CALTS complies with the receiving antenna height criterion for a maximum in the SA if at the frequencies f_s given in 4.4.3.2a):

$$|h_{rc}(m) - h_{r,max}(m)| < T_{hr}(m) - \Delta h_{rm}(m) \quad (7)$$

where

- $h_{rc}(m)$ is the theoretical height of the receiving antenna at which the maximum in the SA occurs, i.e. the minimum in the signal transfer, calculated as depicted in annex C, using the test antenna data after the application of 4.3.2.7 and using the actual geometrical parameters L_a , d , h_t , and the actual frequency f_s ;
- $h_{r,max}(m)$ is the measured receiving antenna height following the procedure outlined in 4.4.5;
- $\Delta h_{rm}(m)$ is the receiving antenna height measurement uncertainty (95 % confidence level) as derived in 4.5.2.4;
- $T_{hr}(m)$ is the allowed tolerance of $h_{r,max}$.

Unless stated otherwise in the antenna calibration standard requiring the use of a CALTS, the allowed tolerance is $T_{hr} = 0,05$ m.

NOTE Either 4.5.3.2 or 4.5.3.3 is applicable; see also 4.4.3.2.

4.5.3.3 The CALTS complies with the frequency criterion for a maximum in the SA if, at the receiving antenna heights h_{rs} , with the antennas tuned to the associated frequencies f_s listed in 4.4.3.2 b)

$$|f_c(\text{MHz}) - f_{\max}(\text{MHz})| < T_f - \Delta f_m(\text{MHz}) \quad (8)$$

where

- $f_c(\text{MHz})$ is the theoretical frequency at which the maximum in the SA occurs, i.e. the minimum in the signal transfer, calculated as depicted in annex C, using the test antenna data following after the application of 4.3.2.7 and using the actual geometrical parameters L_a , d , h_t and h_{rs} ;
- $f_{\max}(\text{MHz})$ is the measured frequency following the procedure outlined in 4.4.6;
- $\Delta f_m(\text{MHz})$ is the frequency measurement uncertainty (95 % confidence level) as derived in 4.5.2.6;
- T_f is the allowed tolerance of $f_{\max}$.

Unless stated otherwise in the antenna calibration standard requiring the use of a CALTS, the allowed tolerance $T_f = 0,03 f_c$.

NOTE Either 4.5.3.2 or 4.5.3.3 is applicable; see also 4.4.3.2.

4.6 The validation report

4.6.1 Introduction

This standard specifies the requirements, the validation procedure and the compliance criteria for a CALTS. This validation process is finalized by the editing and approval of a so-called "CALTS validation report".

This validation report is a means to trace and guarantee the compliance with the CALTS requirements set in this standard.

Either the CALTS owner or other parties may be responsible for the actual demonstration of the validity of the CALTS.

The CALTS validation report shall comply with the requirements given in 4.6.2.

4.6.2 Validation report requirements

The CALTS validation report shall address a number of items, each of them dealing with a validation aspect of the CALTS. Each item and the justification for inclusion in the validation report are described below. A summarizing checklist for the items to be addressed is given in annex F.

a) General information

General information such as the CALTS location, responsible owner, etc. shall be given.

If the site validation is carried out by other parties/organizations, then these parties/organizations shall be indicated.

The CALTS configuration shall be described, as well as its ancillary components using drawings, photographs, part numbers, etc.

In addition, the date(s) of the validation actions and the issue date of the validation report shall be given. The names of the responsible persons for the editing and authorization of the validation report shall be visible on a cover page, including their signatures.

b) Assessment of the validity period and limiting conditions

It is stated that the validity shall be demonstrated prior to the calibration of the antennas (see 4.2.2 a).

Therefore, it is important to indicate the period of anticipated validity of the CALTS under consideration. As the CALTS may be either an indoor or outdoor facility, the anticipated validity of the CALTS may differ and may be affected by different factors such as environmental changes, ageing of cables or ageing of the absorber. It is the responsibility of the facility owner to assess and declare the period of validity of the CALTS validation.

In relation to this validity assessment, items or aspects shall be identified which may be subject to change during the course of use of the facility: for example for outdoor ranges the environment, trees, snow, ground humidity, etc. In general, the performance stability of cabling, equipment, antennas and antenna masts is of importance. Also environmental conditions, ageing of instruments or absorber and validity of calibration of equipment may determine the period of validity of the CALTS.

Quick measurement aids or visual inspection procedures may be incorporated to assess continuously the validity/similarity of the CALTS performance.

Specific environmental or configuration conditions or limitations shall be stated explicitly.

c) Test antenna description and validation

This item of the validation report deals with the demonstration of compliance with the antenna requirements.

The test antennas (elements and baluns) shall comply with the normative specifications given in 4.3.2. and the applicable values given in table 2.

Each of the normative specification items shall be checked against compliance either by inspection or measurement. The compliance verification results shall be available in an annex or in a separate document (photographs, measurement results, calibration results, supplier statements, etc.).

d) The test set-up

This item of the validation report deals with the evidence on the test set-up. The test set-up shall comply with the normative specifications given in 4.4.2 and the applicable values given in table 2.

Each of the normative specifications shall be checked for compliance either by inspection or measurement. The compliance verification results shall be available in an annex or in a separate document.

e) Validation measurements

The results of the site attenuation validation measurements carried out in accordance with the procedure given in 4.4.4 and at the test frequencies and antenna heights given in table 1 shall be described in this section of the validation report. In addition, the results of either the antenna height scan measurements (4.4.5) or the frequency scan measurements (4.4.6) shall be reported in this item.

f) Calculation site antenna attenuation and tolerances

This item in the validation report shall indicate whether the antenna length is calculated using the procedures from annex C or using different numerical procedures. The results of the site attenuation calculations and the results of the total measurement uncertainty calculations shall be presented in this item using default values or calculated values in case of deviations with the tolerances in table 2.

g) Compliance criteria calculations

In this item of the validation report, the results of the calculated and measured values of the SA, and the corresponding allowed tolerances and uncertainties will be used in equation (6) to determine compliance as a function of frequency. Similarly, compliance with either the height criterion (equation (7)) or the frequency-scan criterion (equation (8)) will be determined.

h) Final statement of compliance

Provided the measured site attenuation complies with equation (6) at all frequencies and either the height or the frequency scan criteria conditions are met, then the CALTS under consideration can be declared compliant with the CALTS requirements taking into account the period of validity and the stated limiting conditions and configurations given in item b).

4.7 Validation of the CALTS for vertical polarization

Under consideration.

4.7.1 Introduction**4.7.2 Site specification****4.7.3 Validation procedure****4.7.4 Compliance criteria****4.7.5 Validation report**

Annex A (informative)

CALTS requirements

A.1 Introduction

The normative specifications mean that, in general, a CALTS will also be an open area test-site (OATS). However, normative specifications do not require that a CALTS shall always be an OATS. Consequently, a CALTS may be weather protected, located in a large salt mine, etc., as long as all normative specifications are met.

Test-site details may be found in clause 5 of CISPR 16-1-4, while additional information is given below. Particular care has been taken to supply the user of this standard with a reference list (see clause A.4).

A.2 The reflecting plane

A.2.1 Reflecting plane construction

The plane material can be a solid sheet or a wire mesh. The sheet or the mesh should preferably be continuously welded at the seams, or at distances along the seams $< \lambda_{\min}/10$, where $\lambda_{\min}$ is the wavelength associated with the largest frequency to be considered. If a wire mesh is chosen, care must be taken that the crossing wires make good conductive contact with each other. The mesh width should be $< \lambda_{\min}/10$.

The thickness of the material is determined by mechanical strength and stability requirements. A conductivity equal to or better than that of iron is sufficiently high. The shape of the plane is not very critical as long as the plane is not elliptical (see A.2.2). The reflecting plane should not be covered by a protective layer of significant thickness, as this layer may alter the phase of the reflected wave, i.e. it causes ϕ in 4.4.1 to differ from π radians [A.4]*. For information about the flatness and roughness of the plane, see clause 5 of CISPR 16-1-4 and [A.3]. A flatness of ± 10 mm will normally suffice for measurements up to 1 000 MHz.

The horizontal dimensions of the plane have to be large enough that the influence of the finite plane dimensions on the uncertainty margin associated with the antenna calibration is sufficiently low. Unfortunately, as yet no theoretical models are available which relate the minimum horizontal plane dimensions to a specified maximum uncertainty margin as a result of an antenna calibration. A possible criterion is that the first Fresnel zone should be incorporated in the reflecting plane ([A.1], [A.2] and [A.3]). This leads to a plane with minimum dimensions of 20 m (length) by 15 m (width), but a smaller plane might also meet the CALTS requirements. At the lowest frequency (30 MHz) the length L_a of the test antenna is about 5 m. So, in the case of a 20 m by 15 m plane, the distance between the projection of the validation set-up on the plane and a plane edge is at least L_a at all frequencies in the range 30 MHz to 1 000 MHz.

* References in square brackets refer to the reference documents found under clause A.4.

A.2.2 Plane-edge effects and plane surroundings

When limiting the dimensions of the reflecting plane, the edge of that plane automatically presents a transition to a medium with different reflecting properties, so that the EM waves may be scattered at that edge and cause an unwanted influence on the measuring results. Edge diffraction is usually noticed for vertically polarized results, but is negligible for horizontally polarized results [A.7].

Among other things, the amount of scattering depends on whether the reflecting plane is in the same plane as the surrounding soil (wet or dry soil may already introduce a difference [A.5]) or the reflecting plane is elevated, e.g. it is located on a roof top. Results of investigations can be found in [A.6], where it is also demonstrated that the reflecting plane should never have the shape of the first Fresnel ellipse, as in that case the uncertainties introduced by the scattering at the edge may accumulate.

The edge of the reflecting plane may be multi-point earthed to the surrounding soil and if the soil has good conductivity, e.g. when wet, it forms a good extension to the metal reflecting plane [A.7].

If potentially reflective obstacles are within a distance of, say, 40 m from the boundaries of the reflecting plane, it should be verified that the influence of these obstacles can be ignored. This verification might be performed by means of swept-frequency measurements using fixed length dipoles. Such measurements are comparable to those described in 4.4.6. A possible choice of fixed length antenna (tuned to the frequency f_r), associated swept-frequency range and fixed height h_r of the receiving antenna in the case of a transmitting antenna at $h_t = 2$ m is given in table A.1. The broadband approach is calculable using numerical techniques such as the NEC (see clause C.3) [C.5]).

Table A.1 – Combinations of fixed-length dipole antenna, swept-frequency range and receiving antenna height

f_r MHz	B_s MHz	h_r m
60	30 to 100	4,0
180	100 to 300	1,8
400	300 to 600	1,2
700	600 to 1 000	1,4

In the absence of anomalies, the response will vary in a smooth way. In the presence of anomalies, relatively narrow-band resonances will be superimposed on this response. These resonances identify exact frequencies where the reflections from obstacles are worse. The location of a suspected obstacle can be verified at these frequencies by exaggerating its effect by placing a large metal plate in front of it, oriented at an angle that gives maximum effect.

A.3 Ancillary equipment

Care should be taken that antenna mast material, adaptors, rope, effects of wetness of masts and ropes, guiding of the cables, connectors, possible presence of a turntable if the CALTS is also used as a COMTS do not influence the measurement results. Also, in these cases, swept frequency measurements as mentioned in A.2 may reveal possible problems.

A.4 Reference documents

- [A.1] ANSI Standard C63.4, 1992, *Methods of Measurement of Radio-Noise Emissions from Low-Voltage Electrical and Electronic Equipment in the range of 9 kHz to 40 GHz*, 1992.
- [A.2] *Microwave Antenna Measurements*, Hollis, J.S., Lion T.J. and Clayton L. (Editors), Scientific Atlanta Inc., Atlanta, GA, U.S.A., 1986.
- [A.3] *Transmission and Propagation of Electromagnetic Waves*, Sander K.F. and Reed G.A.L., Cambridge University Press, Cambridge, UK, 1987.
- [A.4] *Note on the Open-Field Site Characterization*, Livshits B. and Harpell K., IEEE EMC Symposium, Denver, pp 352-355, 1992.
- [A.5] *Site Attenuation for Various Ground Conditions*, Sugiura A., Shimizu Y. and Yamanaka Y., Trans. IEICE, E73, 9, pp 1517-1523, September 1990.
- [A.6] *Ground-Plane Size and Shape experiments for Radiated Electromagnetic Emission Measurements*, Berquist A.P. and Bennett W.S., EMC/ESD Symposium, Denver, U.S.A. pp 211-217, 1992.
- [A.7] *EMC Antenna Calibration and the Design of an Open-Field Site*, Salter M.J. and Alexander M.J., Meas. Sci. Technol., 2, pp 510-519, 1991.
- [A.8] *Calibration of Antennas used for Radiated Emission Measurements in Electromagnetic Interference (EMI) Control*, ANSI Standard C63.5, 1988.

Annex B (informative)

Test antenna considerations

An example of a test antenna is presented in clause B.1, while clause B.2 discusses the determination of the balun properties from S-parameter measurements, and/or from injection measurements, as mentioned in 4.3.2.6.

B.1 Example of a test antenna

An example of a test antenna, based on [B.1]*, is shown in figure B.1. The balun of the antenna consists of the following:

- a) a 180° 3 dB hybrid coupler of which the sum port (Σ) is always terminated in the characteristic load impedance (assumed to be 50 Ω), and the difference port (Δ) is the input/ output port of the test antenna;
- b) semi-rigid coaxial cables connected to the balanced ports A and B of the hybrid coupler via high quality connectors, e.g. SMA connectors. The cables have a length of approximately 1 m, where this length is also used to distance the wire antenna from mast and coupler reflections;
- c) ferrite beads (F) around the semi-rigid cables to limit the induction of common-mode currents on the balun and the connected antenna cable;
- d) 3 dB attenuators at the output end of the semi-rigid cables acting as impedance stabilizing or matching pads (M), to which the wire elements are attached via SMA connectors. These connectors form the A and B ports (or C and D ports) mentioned in 4.4.4 and annex C. The external conductors of these connectors are in electrical contact near the wire antenna. This contact point is the reference point of the balun when performing S-parameter measurements.

It should be noted that the aforementioned balun is just an example of a useful balun. Other types of balun may be used as well. In fact every type is allowed, provided the requirements set out in 4.3.2 are met.

The wire elements should have a length such that after attachment the test antenna meets the $L_a(f)$ requirement as set out in 4.3.2.2 (see C.1.1 for the calculation of $L_a(f)$). In table C.1 it has been assumed that if $f < 180$ MHz the diameter of the wire elements is 10 mm, thus giving the relatively long wire antennas a good mechanical strength. In table C.1 it has also been assumed that at frequencies $f \geq 180$ MHz an element diameter of 3 mm is sufficient. At frequencies $f < 60$ MHz, the elements might be telescopic, or use might be made of a fixed length dipole antenna (see annex D).

B.2 Determination balun properties

B.2.1 The ideal, loss-less balun

The ideal, loss-less balun is characterized by having signals at the A and B ports that are exactly equal in amplitude and exactly 180° out of phase, provided all three ports (see

* References in square brackets refer to the reference documents given in clause B.3.

The diagram illustrates a balun circuit. It begins with an input/output port connected to a transformer with primary turns Δ and secondary turns Σ . The secondary is connected to a $50\ \Omega$ load. The output of the transformer is connected to a balun section, which consists of two parallel semi-rigid coaxial cables. The top cable has a length L_{we} and is terminated at a distance L_a from the reference point. The bottom cable has a length L_g and is terminated at a distance L_a from the reference point. The balun section is connected to a reference point, which is connected to a diode D_{we} . The diode is connected to a ground plane. The balun section is labeled "Balun" and "Reference point".

M = matching pad

NOTE The balun uses a coaxial hybrid junction.

Figure B.1 – Example of a test antenna

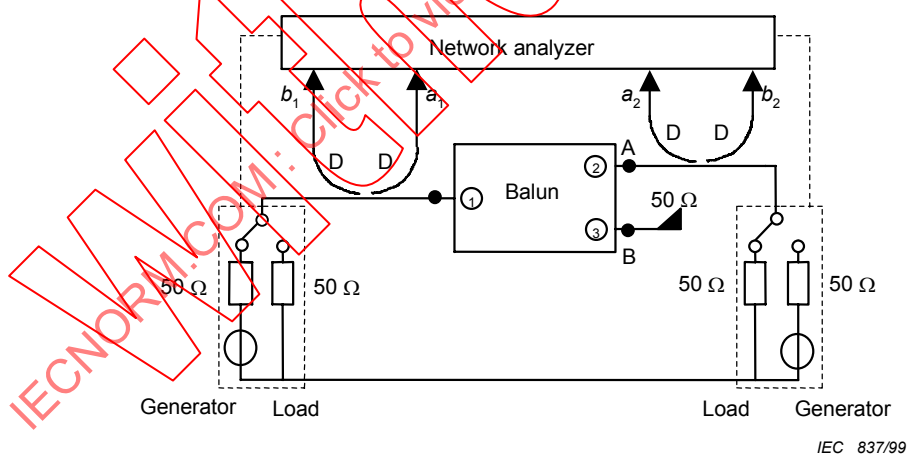


Figure B.2 – Diagram of the measurement of S_{11} and S_{12} and of S_{22} and S_{21} when generator and load are interchanged (in this figure by putting both switches in their alternative position)

The basic set-up to measure S-parameters is given in figure B.2. The unbalanced input/output port of the balun is numbered "1", and the balanced ports are numbered "2" and "3".

It is assumed that the characteristic impedance of each these three ports equals $50\ \Omega$ (see 4.3.2.5). Compared to figure B.1, the complete balun (coupler, cables, etc.) is represented in figure B.2 by the single box labelled "Balun". The Σ -port of the hybrid coupler in figure B.1 is always terminated in its characteristic impedance and, hence, does not play a part.

S-parameters give the relation between the incoming waves represented in figure B.2 by a_1 or a_2 and the scattered waves represented by b_1 and b_2 . The incoming and scattered signals are measured by the analyser via directional couplers (D). The parameters $S_{11} = b_1/a_1$ and $S_{21} = b_2/a_1$ (under the condition $a_2 = 0$) are measured with port 3 terminated in $50\ \Omega$. Interchanging the generator and load (by changing the position of both switches) results in the measurement of $S_{22} = b_2/a_2$ and $S_{12} = b_1/a_2$ (under the condition $a_1 = 0$). Similarly, terminating port 2 with the $50\ \Omega$ load and measuring between ports 1 and 3, yields S_{11} , and S_{13} , S_{31} and S_{33} . Finally, terminating port 1 with the $50\ \Omega$ load and measuring between ports 2 and 3, yields (again) S_{22} and S_{33} , and S_{23} and S_{32} .

The S-parameter matrix for the ideal, loss-less balun is given by the following equation:

$$\begin{pmatrix} S_{11} & S_{12} & S_{13} \\ S_{21} & S_{22} & S_{23} \\ S_{31} & S_{32} & S_{33} \end{pmatrix} = \frac{1}{\sqrt{2}} \begin{pmatrix} 0 & 1 & -1 \\ 1 & 0 & 0 \\ -1 & 0 & 0 \end{pmatrix} \quad (\text{B.1})$$

In this S-matrix, $S_{11} = S_{22} = S_{33} = 0$ since there is no reflection at the ports. $S_{12} = S_{21} = 1$ and $S_{13} = S_{31} = -1$ as the balance is perfect (equal absolute values equal to 1 as this balun is loss-less) and the phase shift equals exactly 180° (indicated by the minus sign). Finally, $S_{23} = S_{32} = 0$ as the isolation between port 2 and port 3 is perfect.

B.2.2 Relations between balun properties and S-parameters

The S-matrix can be transformed into an impedance matrix, which relates the input and output currents and voltages of the balun. Terminating port 1 in the characteristic impedance and considering ports 2 and 3 only, it can be shown that (see [B.2]):

$$\begin{pmatrix} Z_{22} & Z_{23} \\ Z_{32} & Z_{33} \end{pmatrix} = \frac{50}{(1 - S_{22})(1 - S_{33}) - S_{23} S_{32}} \cdot \begin{pmatrix} [(1 + S_{22})(1 - S_{33}) + S_{23} S_{32}] & 2 S_{32} \\ 2 S_{23} & [(1 - S_{22})(1 + S_{33}) + S_{23} S_{32}] \end{pmatrix} \quad (\text{B.2})$$

so that the impedance Z_{AB} (see 4.3.2.5 a)) is given by the following equation:

$$Z_{AB} = \frac{1 - S_{22} S_{33} + S_{23} S_{32} - S_{23} - S_{32}}{(1 - S_{22})(1 - S_{33}) - S_{23} S_{32}} 100 = R_{AB} + j X_{AB} \quad (B.3)$$

The measured value of Z_{AB} is needed in the calculation of SA_c (see annex C). The impedance Z_{CD} for the other balun needed in that calculation is determined similarly.

The associated VSWR complies with 4.3.2.5 a) and table 2 if

$$\frac{1 + |\Gamma|}{1 - |\Gamma|} < 1,10, \text{ where } \Gamma = \frac{Z_{AB} - 100}{Z_{AB} + 100} \quad (B.4)$$

NOTE If the hybrid coupler itself does not comply with the requirement formulated in equation (B.4), the VSWR can be lowered by using matched attenuators (M in figure B.1) with very low VSWR.

The balance and phase shift of an actual balun is verified by considering

$$\frac{S_{12}}{S_{13}} = \frac{S_{21}}{S_{31}} = r_b e^{j\phi_b} \quad (B.5)$$

The amplitude balance complies with 4.3.2.5 b) and table 2 if

$$0,95 < r_b < 1,05 \quad (B.6)$$

and the phase balance complies with 4.3.2.5 c) and table 2 if

$$178^\circ < \left| \frac{180 \phi_b}{\pi} \right| < 182^\circ \quad (B.7)$$

The isolation of an actual balun is verified by considering the actual value of S_{23} and S_{32} . It complies with 4.3.2.5, note 4 if

$$|S_{23}| = |S_{32}| < 0,05 \quad (B.8)$$

The possible loss in the actual balun is accounted for during measurement of the reference voltage U_r in the CALTS validation procedure. For the balun used in the example and depicted in figure B.1, an important contribution to the loss stems from the 3 dB matching pads.

B.2.3 Insertion loss measurements

It is also possible to verify the balun specifications set in 4.3.2.5 b) and 4.3.2.5 c) by performing the insertion loss measurements depicted in figures B.3 and B.4. From the results, the so-called balun unbalance rejection (*BUR*) can be determined.

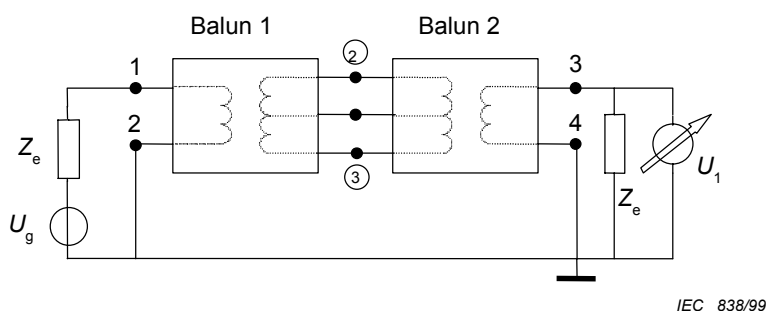


Figure B.3 – Schematic diagram of the determination of the insertion loss $A_1(f)$

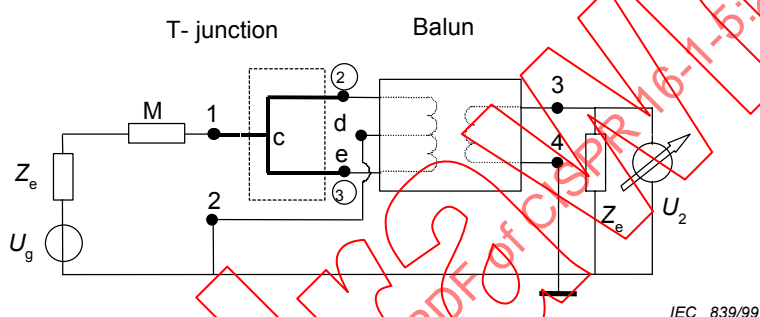


Figure B.4 – Schematic diagram of the determination of the insertion loss $A_2(f)$

The measurements comprise the determination of the insertion loss $A_1(f)$ of two identical baluns connected head-to-head as in 4.4.4.1, and the determination of the insertion loss $A_2(f)$ for a single balun when the balanced ports 2 and 3 (see also figure B.4) are connected in parallel. Assuming that A_1 stems from equal contributions of the two baluns, the balun unbalance rejection, also referred to as the common-mode rejection, expressed in decibels is given by the following equation:

$$BUR(f) = A_2(f) - \frac{A_1(f)}{2} \quad (\text{dB}) \quad (\text{B.9})$$

It can be shown that the balun complies with the aforementioned clauses and the associated numerical values of the tolerances as given in table 2 when $BUR > 28$ dB.

In the first insertion loss measurement, firstly the reference voltage $U_{r1}(f)$ is determined as a function of frequency over the frequency band specified for the balun. The measuring circuit is that of figure B.3 in the absence of the two baluns but with a short circuit between the connection points 1 and 3 and 2 and 4. Next, the voltage $U_1(f)$ is measured after insertion of the two baluns connected head-to-head (see figure B.3). Then $A_1(f)$ expressed in decibels is given by the following equation:

$$A_1(f) = 20 \log_{10} \left(\frac{U_{r1}(f)}{U_1(f)} \right) \quad (\text{dB}) \quad (\text{B.10})$$

In the second insertion loss measurement, firstly the reference voltage $U_{r2}(f)$ is determined as a function of frequency over the frequency band specified for the balun. The measuring circuit is that of figure B.4 in the absence of the T-junction and the balun but with a short circuit between the connection points 1 and 3 and 2 and 4. Next, the voltage $U_{2a}(f)$ is measured after insertion of the T-junction and the balun to be verified (see figure B.4). In this measurement the ports 2 and 3 (see also figure B.2) are connected in parallel via a coaxial symmetrical T-junction constructed of semi-rigid cables and having the same electrical length of the parts c-d and c-e of the T (full mechanical symmetry). In this measurement d is connected to port 2 and e to port 3. The 6 dB matched attenuator pad, indicated in figure B.4 by M, has been added to avoid standing wave effects.

To avoid errors caused by parasitic effects, the latter measurement is repeated after reversing the connection between the balun and T-junction, i.e. d is connected to port 3 and e to port 2. This measurement yields the voltage $U_{2b}(f)$. Then $A_2(f)$ expressed in decibels is given by the following equation:

$$A_2(f) = 20 \log_{10} \left(\frac{U_{r2}}{\max\{U_{2a}(f), U_{2b}(f)\}} \right) \quad (\text{B.11})$$

For the ideal balun $A_2(f) = \infty$ dB, at all frequencies.

NOTE Instead of this T-junction plus 6 dB attenuator, a calibrated 6 dB power divider may be used. In this case, the attenuation caused by the power divider should be taken into account in the calculation of the BUR.

B.3 Reference documents

- [B.1] *Standard Linear Antennas, 30-1 000 MHz*, FiltzGerell R.G., IEEE Trans. on Antennas and Propagation, **AP-34**, 12, pp 1425-1429, December 1986.
- [B.2] *Microwave Impedance Measurement*, Somlo P.I., Hunter J.D., published by Peter Peregrinus Ltd., London, UK, 1985.
- [B.3] *Low Measurement Uncertainties in the Frequency Range 30 MHz to 1 GHz using Calculable Standard Dipole Antenna and National Reference Ground Plane*, Alexander M.J. and Salter M.J., IEE Proc. Sci. Meas. Technol., Vol. 143, no. 4, pp 221 – 228, July 1996.

Annex C (informative)

Antenna and site attenuation theory

C.1 Analytical relations

This clause gives an analytical approach to the calculation of the total length $L_a(f)$ of the wire antenna (C.1.1) and the site attenuation SA_c (C.1.2). The model takes into account the mutual coupling between the transmitting antenna, the receiving antenna and their images in the reflecting plane. It also accounts for the actual field distribution along the receiving antenna, i.e. it is not assumed that the field arriving at the receiving antenna is a plane wave. The only assumption made in this approach is that the current distribution over the wire antenna is sinusoidal.

A value of SA_c calculated from the analytical relations is within ± 0.01 dB of the value of SA_c obtained from exact numerical calculations provided the value of L_a of a sufficiently thin wire antenna is used in the analytical approach. In the context of this standard, sufficiently thin means that the radius R_{we} of the wire antenna satisfies the following condition [C.1]*:

$$\alpha = 2 \ln \left(\frac{L_a}{R_{we}} \right) \text{ with } \alpha \geq 30$$

For a half-wavelength dipole antenna ($L_a = \lambda_0/2$) this condition is given by the following equation:

$$R_{we} = \frac{\lambda_0}{2\sqrt{e}^\alpha} \text{ with } \alpha \geq 30 \quad (C.1)$$

A complete numerical example, including measurement uncertainty considerations is given in C.1.3. Annex E gives an example of a computer program to calculate the various quantities.

C.1.1 Total length of the test antenna

By definition, the total length $L_a(f)$ of the test antenna, i.e. the free-space resonant dipole at the frequency f follows when solving the following equation:

$$X_a(f, R_{we}) = 0 \quad (C.2)$$

where

$X_a(f, R_{we})$ is the imaginary part of the impedance of that dipole radiating into an unbounded medium, i.e. in free space;

R_{we} is the radius of a wire element, assumed to be a constant along its length (non-telescopic elements) and to be much smaller than L_a .

* References in square brackets refer to the reference documents given in clause C.3.

The feed-point gap W_g is assumed to be infinitely small. X_a is given by the following equation (see [C.2]):

$$X_a = \frac{\eta}{4\pi} \times [2 \operatorname{Si}(kL_a) + \cos(kL_a) \times \{2 \operatorname{Si}(kL_a) - \operatorname{Si}(2kL_a)\} - \sin(kL_a) \{2 \operatorname{Ci}(kL_a) - \operatorname{Ci}(kL_a) - \operatorname{Ci}(2kR_{we}^2/L_a)\}] \times \sin^{-2}(kL_a/2) \quad (\text{C.3})$$

where

$$\eta = 377 \, \Omega;$$

$$k = 2\pi/\lambda_0; \text{ and}$$

λ_0 the wavelength in vacuum.

$\operatorname{Si}(x)$ and $\operatorname{Ci}(x)$ are given by the following equations:

$$\operatorname{Si}(x) = \int_0^x \frac{\sin(\tau)}{\tau} d\tau \quad (\text{C.4a})$$

$$\operatorname{Ci}(x) = \int_{-\infty}^x \frac{\cos(\tau)}{\tau} d\tau \quad (\text{C.4b})$$

$$\begin{aligned} \operatorname{Si}(x) &= \frac{\pi}{2} - f(x) \cos x - g(x) \sin x \quad (x \geq 1) \\ \operatorname{Si}(x) &= \sum_{n=0}^{\infty} \frac{(-1)^n x^{2n+1}}{(2n+1)(2n+1)!} \quad (x < 1) \end{aligned} \quad (\text{C.5a})$$

and can be calculated sufficiently accurately from [C.3]

$$\begin{aligned} \operatorname{Ci}(x) &= f(x) \sin x - g(x) \cos x \quad (x \geq 1) \\ \operatorname{Ci}(x) &= \gamma + \ln x + \sum_{n=1}^{\infty} \frac{(-1)^n x^{2n}}{2n (2n)!} \quad (x < 1) \end{aligned} \quad (\text{C.5b})$$

$$f(x) = \frac{1}{x} \left(\frac{x^4 + a_1 x^2 + a_2}{x^4 + b_1 x^2 + b_2} \right), g(x) = \frac{1}{x^2} \left(\frac{x^4 + c_1 x^2 + c_2}{x^4 + d_1 x^2 + d_2} \right) \quad (\text{C.5c})$$

$$\begin{aligned} \text{with } a_1 &= 7,241163 & b_1 &= 9,068580 & c_1 &= 7,547478 & d_1 &= 12,723684 \\ a_2 &= 2,463936 & b_2 &= 7,157433 & c_2 &= 1,564072 & d_2 &= 15,723606 \end{aligned}$$

The $L_a(f)$ data in table C.1 have been derived from equation (C.2), using equations (C.3) to (C.5).

C.1.2 Theoretical site attenuation

The site attenuation (SA) is calculated by using a network model [C.4] (see figure C.1). The RF generator supplies a signal to the feed terminals A and B at the balun of the transmitting antenna. The signal arriving at the feed terminals C and D of the receiving antenna is measured across the receiver impedance Z_r . The cables and baluns are represented by the T-networks.

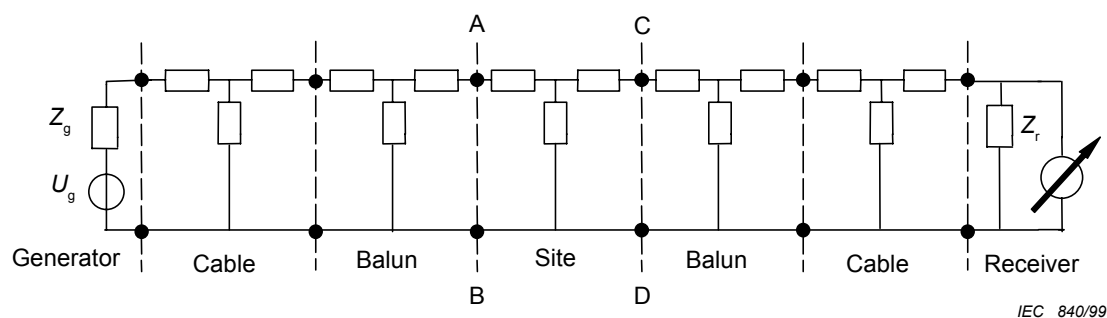


Figure C.1 – Network model for SA calculations

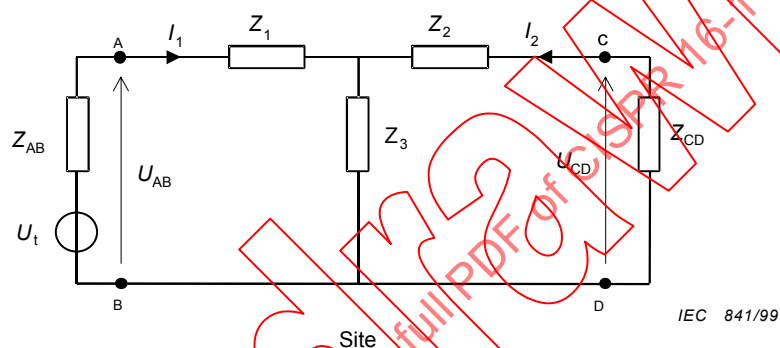


Figure C.2 – Equivalent circuit to the network in figure C.1

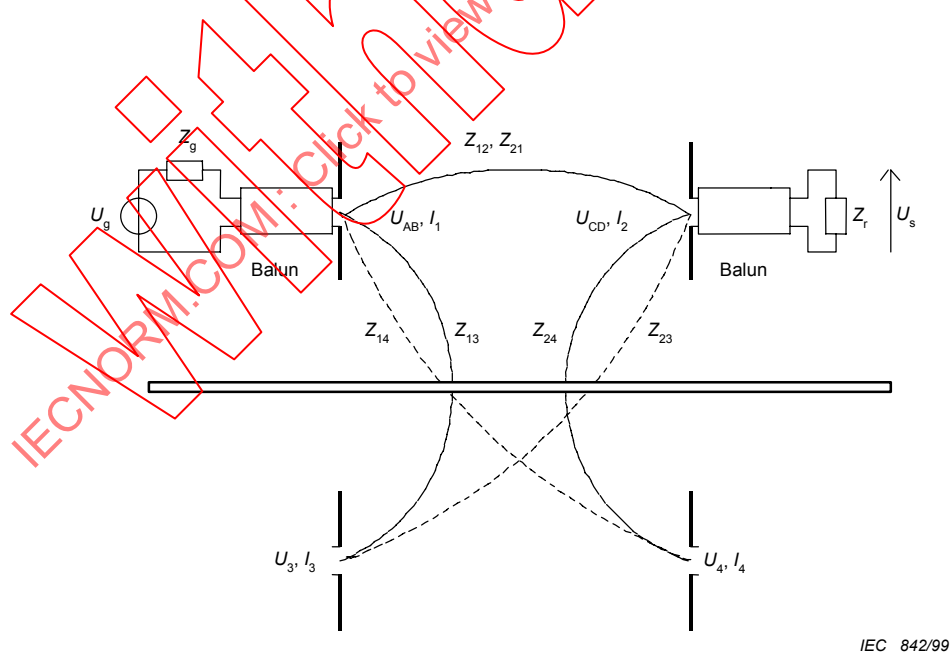


Figure C.3 – Definition of the mutual couplings, feed-terminal voltages and antenna currents of the antennas above the reflecting plane and their images

When the reference voltages $U_{r1}(f)$ and $U_{r2}(f)$ (see 4.4.4.1 and 4.4.4.4) are measured, the feed terminals A and C are interconnected by a short conductor having a negligible impedance. Similarly, B and D are interconnected. When measuring $U_s(f)$ (see 4.4.4.3), with the wire antennas connected to the feed terminals and the test antennas in their specified positions, the influence of the site on the signal transfer is represented by a T-network with ports AB and CD as shown in figure C.1.

The circuit of figure C.1 can be simplified to that of figure C.2, in which Z_{AB} and Z_{CD} are the measured balanced-port impedances (see annex B). From the circuit in figure C.2 it follows that when measuring the reference voltage U_r (so that $Z_1 = Z_2 = 0$ and $Z_3 = \infty$):

$$U_{CD} = U_{CD,r} = \frac{Z_{CD}}{Z_{AB} + Z_{CD}} U_t \quad (C.6)$$

It also follows that when measuring U_s

$$U_{CD} = U_{CD,s} = \frac{Z_{CD} Z_3}{(Z_{AB} + Z_1 + Z_3)(Z_{CD} + Z_2 + Z_3) - Z_3^2} U_t \quad (C.7)$$

so that the calculated site attenuation SA_c is given by

$$SA_c = \frac{U_{CD,r}}{U_{CD,s}} = \frac{(Z_{AB} + Z_1 + Z_3)(Z_{CD} + Z_2 + Z_3) - Z_3^2}{Z_3(Z_{AB} + Z_{CD})} \quad (C.8)$$

The next step is to relate the impedances Z_1 , Z_2 and Z_3 to the actual situation as depicted in figure C.3, i.e. to the two test antennas above the reflecting plane.

The signal transfer between the transmitting port 1 (feed terminals A and B) and the receiving port 2 (feed terminals C and D) is influenced by the various couplings between the antennas and their images. In figure C.3 this is indicated by the transfer impedances Z_{nm} (n, m : 1 to 4, $n \neq m$).

The terminal voltages U_{AB} and U_{CD} are formally related to the antenna currents I_1 through I_4 of the four antennas in figure C.3 via

$$\begin{aligned} U_{AB} &= Z_{11} I_1 + Z_{12} I_2 + Z_{13} I_3 + Z_{14} I_4 \\ U_{CD} &= Z_{21} I_1 + Z_{22} I_2 + Z_{23} I_3 + Z_{24} I_4 \end{aligned} \quad (C.9)$$

For the theoretical reflecting plane and in the case of horizontally polarized antennas which are aligned parallel to each other $I_3 = \rho I_1$ and $I_4 = \rho I_2$, where $\rho = re^{j\phi}$ is the complex reflection coefficient of the conducting plane. In the ideal case, $\rho = -1$ in the present configuration. Moreover, because of reciprocity $Z_{12} = Z_{21}$ and $Z_{23} = Z_{14}$. So equation (C.9) reduces to the following:

$$\begin{aligned} U_{AB} &= (Z_{11} + \rho Z_{13}) I_1 + (Z_{12} + \rho Z_{14}) I_2 \\ U_{CD} &= (Z_{12} + \rho Z_{14}) I_1 + (Z_{22} + \rho Z_{24}) I_2 \end{aligned} \quad (C.10)$$

From the circuit in figure C.2 it follows that

$$\begin{aligned} U_{AB} &= (Z_1 + Z_3)I_1 + Z_3 I_2 \\ U_{CD} &= Z_3 I_1 + (Z_2 + Z_3)I_2 \end{aligned} \quad (C.11)$$

and comparison with equation (C.10) yields

$$Z_1 + Z_3 = Z_{11} + \rho Z_{13}, \quad Z_2 + Z_3 = Z_{22} + \rho Z_{24} \quad \text{and} \quad Z_3 = Z_{12} + \rho Z_{14}$$

so that equation (C.8) can be rewritten as

$$SA_c = \frac{(Z_{AB} + Z_{11} + \rho Z_{13})(Z_{CD} + Z_{22} + \rho Z_{24}) - (Z_{12} + \rho Z_{14})^2}{(Z_{12} + \rho Z_{14})(Z_{AB} + Z_{CD})} \quad (C.12)$$

From equation (C.9) it follows that Z_{11} and Z_{22} are the input impedance of the wire antenna radiating into free space, thus in absence of the reflecting plane. The imaginary part of these impedances can be calculated from $X_{11} = X_{22} = X_a$ as given by equation (C.3), the real part $R_{11} = R_{22} = R_a$ from the following:

$$\begin{aligned} R_a &= \frac{\eta}{2\pi} \left\{ \gamma + \ln(kL_a) - Ci(kL_a) \right. \\ &\quad + \frac{1}{2} \sin(kL_a) \times [Si(2kL_a) - 2Si(kL_a)] \\ &\quad \left. + \frac{1}{2} \cos(kL_a) \times [\gamma + \ln(kL_a/2) + Ci(2kL_a) - 2Ci(kL_a)] \right\} \times \sin^{-2}(kL_a/2) \end{aligned} \quad (C.13)$$

The mutual impedances Z_{12} , Z_{13} , Z_{14} and Z_{24} can be calculated with the aid of the Lorentz reciprocity theorem [C.1, C.2]. In this calculation the actual field along the wire antenna is taken into account, thus eliminating the need to assume a plane wave arriving at the receiving antenna. The only assumption made is that the current distribution on the wire antennas is sinusoidal, which is allowed if $L_a(r) \approx \lambda_0/2$ and if R_{we} satisfies the condition given in equation (C.1).

If $Z_{nm} = R_{nm} + jX_{nm}$ ($n = 1, \dots, 4$, $m = 1, \dots, 4$, $n \neq m$) the real part is given by the following [C.1]:

$$\begin{aligned} R_{nm} &= \frac{\eta}{4\pi} \times \left\{ 2[2Ci(kr_{nm}) - Ci(ks_3) - Ci(ks_4)] \right. \\ &\quad + \cos(kL_a) \times [2Ci(kr_{nm}) + Ci(ks_1) + Ci(ks_2) - Ci(ks_3) - 2Ci(ks_4)] + \sin(kL_a) \\ &\quad \left. + \sin(kL_a) \times [Si(ks_1) - Si(ks_2) - 2Si(ks_3) + 2Si(ks_4)] \right\} \times \sin^{-2}(kL_a/2) \end{aligned} \quad (C.14)$$

and the imaginary part by the following:

$$\begin{aligned} X_{nm} &= \frac{-\eta}{4\pi} \times \left\{ 2[2Si(kr_{nm}) - Si(ks_3) - Si(ks_4)] \right. \\ &\quad + \cos(kL_a) \times [2Si(kr_{nm}) + Si(ks_1) + Si(ks_2) - 2Si(ks_3) - 2Si(ks_4)] \\ &\quad \left. - \sin(kL_a) \times [Si(ks_1) - Ci(ks_2) - 2Ci(ks_3) + 2Ci(ks_4)] \right\} \times \sin^{-2}(kL_a/2) \end{aligned} \quad (C.15)$$

where r_{nm} is the distance between the centres of the antennas n and m , and

$$\begin{aligned} s_1 &= \sqrt{r_{nm}^2 + L_a^2} + L_a \\ s_2 &= \sqrt{r_{nm}^2 + L_a^2} - L_a \\ s_3 &= \sqrt{r_{nm}^2 + (L_a / 2)^2} + L_a / 2 \\ s_4 &= \sqrt{r_{nm}^2 + (L_a / 2)^2} - L_a / 2 \end{aligned} \quad (C.16)$$

Now SA_c , as needed in 4.5.3.1, can be calculated from equation (C.12) as all impedances in that equation are known: Z_{AB} and Z_{CD} from experimental data (see annex B), and the other impedances as calculated from equations (C.3) and (C.13) to (C.16). The same equations can be used to calculate $SA_c(h_r)$ at a given frequency, so as to determine $h_{r,max}(f_s)$ as needed in 4.5.3.2, and to calculate the measurement uncertainties ΔSA_t and $\Delta h_{r,max}$ needed in 4.5.2.2 and 4.5.3.2.

C.1.3 Numerical example

Results of a numerical example are given in table C.1: L_a and SA_c calculations; Table C.2: ΔSA_t calculations; table C.3: h_{rc} and Δh_{rt} calculations; and table C.4: f_c and Δf_t calculations. An example of a computer program to calculate these data is given in annex E.

In all calculations the height of the receiving antenna and that of the transmitting antenna, the horizontal distance between the centres of the antennas, and the frequencies have the values specified in 4.4. When performing measurement uncertainty calculations, the tolerances given in 4.5.2.1 have been used.

In the range $30 \text{ MHz} \leq f < 180 \text{ MHz}$ it has been assumed that the radius of the wire antenna $R_{we} = 5,0 \text{ mm}$, and that $R_{we} = 1,5 \text{ mm}$ if $180 \text{ MHz} \leq f \leq 1\,000 \text{ MHz}$.

C.1.3.1 L_a and SA_c calculations (table C.1)

The antenna length $L_a(f)$ has been calculated from equation (C.2). The value of $SA_c(f)$ has been calculated from equations (C.13) to (C.16), assuming ideal baluns with balanced port impedances having the preferred value of $(100 + j0) \Omega$, and assuming an ideal reflecting plane, i.e. $\rho = -1$.

C.1.3.2 ΔSA_t calculations (table C.2)

The measurement uncertainty ΔSA_t (4.5.2.2) with 95 % confidence level can be calculated from the following (see [C.6])

$$\Delta SA_t = \frac{2}{\sqrt{3}} \sqrt{\sum_{i=1}^9 \Delta SA_c^2(i)} \quad (C.17)$$

assuming a rectangular probability distribution of the variables $\Delta SA_c(i)$ and accounting for the uncertainties in the $p = 9$ variables: h_r , h_t , d , f , Z_{AB} , Z_{CD} , L_a , A_b and ϕ_b (see also table 2).

For the first six variables, ΔSA_c can be calculated from

$$SA_c(i) = \text{Max} [\text{Abs}\{SA_c - SA(p_i \pm \Delta p_i)\}] \quad (i = 1, 2, \dots, 6) \quad (\text{C.18})$$

where

SA_c is the nominal value of the site attenuation as calculated in C.1.3.1;

$SA(p_i + \Delta p_i)$ and $SA(p_i - \Delta p_i)$ are the calculated site attenuation for the variable p plus the tolerance Δp and p minus that tolerance.

Results of ΔSA_c caused by Δh_r , Δh_t , Δd and Δf specified in table 2 are given in columns 3 to 6 of table C.2.

NOTE When calculating the effect of Δf , the antenna length L_a remains a constant equal to L_a at the nominal frequency. In the "procedure SA" in the computer program given in annex E, the variable "f0" keeps L_a constant when varying the variable "f" representing the frequency.

Table C.1 – Numerical example, calculation of L_a , SA_c (see C.1.3.1)

f MHz	h_r m	R_{we} mm	L_a m	SA_c dB	f MHz	h_r m	R_{we} mm	L_a m	SA_c dB
30	4,00	5,00	4,803	21,03	160	2,00	5,00	0,885	26,44
35	4,00	5,00	4,112	20,95	180	2,00	1,50	0,797	27,52
40	4,00	5,00	3,594	20,60	200	2,00	1,50	0,716	29,37
45	4,00	5,00	3,192	20,70	250	1,50	1,50	0,572	30,43
50	4,00	5,00	2,870	21,12	300	1,50	1,50	0,476	32,47
60	4,00	5,00	2,388	22,13	400	1,20	1,50	0,355	34,90
70	4,00	5,00	2,043	21,76	500	2,30	1,50	0,283	37,02
80	4,00	5,00	1,785	20,93	600	2,00	1,50	0,236	38,35
90	4,00	5,00	1,585	21,49	700	1,70	1,50	0,201	39,59
100	4,00	5,00	1,425	22,97	800	1,50	1,50	0,176	40,91
120	4,00	5,00	1,185	25,16	900	1,30	1,50	0,156	41,84
140	2,00	5,00	1,013	27,20	1 000	1,20	1,50	0,140	42,71

For the impedances Z_{AB} and Z_{CD} , table 2 specifies a maximum VSWR of 1,10. In the present numerical example this means that both impedances have a circle (centre at $p = 100 + j0 \Omega$, radius $\Delta p = 9,5 \Omega$) as a boundary in the impedance plane. Investigations show that it is sufficient to only perform the calculations for $p = (100 \pm \Delta p + j0)$ and $p = (100 \pm j\Delta p)$. Results of calculations are given in columns 7 and 8. Note that the ΔSA_c values given in table C.2 columns 7 and 8 are equal only when $h_r = h_t$.

ΔSA_c associated with L_a , A_b and ϕ_b can only be estimated via numerical techniques, such as discussed in clause C.2. Using these techniques it is found that $\Delta SA_c(L_a) < 0,03$ dB and that $\Delta SA_c(A_b, \phi_b) < 0,03$ dB.

Table C.2 column 9 gives the root-sum-square (RSS) value $\Delta SA_z = \sqrt{[\sum \Delta SA_c(i)]}$ of the six values ΔSA_c in the preceding columns. The 95 % confidence level values in column 10 follow from multiplying the column 9 data by $2/\sqrt{3}$ (see equation (C.17)). The 95 % confidence level values of ΔSA_t follow from:

$$\Delta SA_t(\text{CL} = 95 \%) = \frac{2}{\sqrt{3}} \sqrt{\left\{ \sum_{i=1}^6 \Delta SA_c^2(i) \right\} + \Delta SA_c^2(L_a) + \Delta SA_c^2(A_b, \phi_b)} \quad (\text{C.19})$$

Assuming $\Delta SA_c(L_a) = 0,03$ dB and $\Delta SA_c(A_b, \phi_b) = 0,03$ dB, the ΔSA_t values given in column 11 follow. In this example, the maximum value equals $\Delta SA_t = 0,19$ dB (at 80 MHz). This is why a value of $\Delta SA_t = 0,20$ dB is mentioned in 4.5.3.1.

Table C.2 – Numerical example, calculation of ΔSA_t (see C.1.3.2)

Frequency MHz	SA_c dB	Δh_r ΔSA_c dB	Δh_t ΔSA_c dB	Δd ΔSA_c dB	Δf ΔSA_c dB	ΔZ_{AB} ΔSA_c dB	ΔZ_{CD} ΔSA_c dB	RSS ΔSA_Σ dB	95 % ΔSA_Σ dB	95 % ΔSA_t dB
30	21,03	0,023	0,018	0,056	0,031	0,110	0,026	0,13	0,15	0,16
35	20,95	0,028	0,020	0,051	0,007	0,080	0,057	0,12	0,13	0,14
40	20,60	0,025	0,024	0,054	0,005	0,059	0,105	0,14	0,16	0,16
45	20,70	0,013	0,028	0,055	0,013	0,036	0,121	0,14	0,16	0,17
50	21,12	0,001	0,033	0,048	0,016	0,010	0,106	0,12	0,14	0,15
60	22,13	0,002	0,044	0,051	0,005	0,027	0,049	0,09	0,10	0,11
70	21,76	0,019	0,050	0,050	0,038	0,061	0,058	0,12	0,14	0,14
80	20,93	0,014	0,041	0,038	0,039	0,104	0,098	0,16	0,18	0,19
90	21,49	0,011	0,012	0,035	0,011	0,121	0,084	0,15	0,18	0,18
100	22,97	0,007	0,021	0,036	0,027	0,106	0,056	0,13	0,15	0,15
120	25,16	0,008	0,039	0,012	0,018	0,051	0,092	0,12	0,13	0,14
140	27,20	0,043	0,043	0,047	0,029	0,055	0,055	0,11	0,13	0,14
160	26,44	0,030	0,032	0,046	0,023	0,097	0,097	0,15	0,18	0,18
180	27,52	0,021	0,021	0,039	0,029	0,086	0,086	0,13	0,16	0,16
200	29,37	0,015	0,015	0,029	0,017	0,057	0,057	0,09	0,10	0,11
250	30,43	0,035	0,019	0,038	0,027	0,089	0,072	0,13	0,15	0,15
300	32,47	0,010	0,008	0,016	0,020	0,075	0,076	0,11	0,13	0,13
400	34,90	0,042	0,054	0,008	0,016	0,084	0,092	0,14	0,16	0,17
500	37,02	0,005	0,006	0,047	0,009	0,068	0,069	0,11	0,12	0,13
600	38,35	0,000	0,004	0,013	0,012	0,075	0,075	0,11	0,12	0,13
700	39,59	0,002	0,046	0,017	0,008	0,080	0,072	0,12	0,14	0,14
800	40,91	0,004	0,051	0,008	0,009	0,071	0,075	0,12	0,13	0,14
900	41,84	0,005	0,018	0,025	0,009	0,075	0,068	0,11	0,12	0,13
1 000	42,71	0,011	0,062	0,004	0,010	0,079	0,075	0,13	0,15	0,15
ΔSA (dB) maximal		0,043	0,062	0,056	0,039	0,121	0,121	0,16	0,18	0,19

NOTE The bottom line in this table gives the maximum value in each column. Three digits behind the comma in columns 3 to 8 have no practical meaning, and are only given for the comparison of calculated results.

C.1.3.3 h_{rc} and Δh_{rt} calculations (table C.3)

This subclause considers $h_{r,max}(f_s)$ as specified in 4.4.3.2 a) and 4.4.5. The value can be found by a procedure which searches for the first sharp maximum in SA for $h_r > 1$ m. Care should be taken that a sharp maximum is found, i.e. a maximum associated with a cancelling of the direct and indirect waves at the receiving antenna. Results of h_{rc} (see 4.5.3.2) at the frequencies f_s specified in 4.4.3.2 a) are given in table C.3.

Also given in table C.3 are the results of measurement uncertainty calculations, yielding $\Delta h_{r,max}$, similar to those given in C.1.3.2, using the tolerances given in table 2. In the case of